

L Number	Hits	Search Text	DB	Time stamp
1	23	(379/27.05).CCLS.	USPAT	2003/07/28 11:32
2	365	(379/412).CCLS.	USPAT	2003/07/28 11:32
3	53	((379/412).CCLS.) and "diode bridge"	USPAT	2003/07/28 11:33
4	126	((379/412).CCLS.) and surge	USPAT	2003/07/28 11:33
5	14	((379/412).CCLS.) and "diode bridge") and ((379/412).CCLS.) and surge)	USPAT	2003/07/28 11:33
6	165	((379/412).CCLS.) and "diode bridge") or ((379/412).CCLS.) and surge)	USPAT	2003/07/28 11:54
7	6	((379/412).CCLS.) and "diode bridge") or ((379/412).CCLS.) and surge)) and emi	USPAT	2003/07/28 12:14
8	200	((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))	USPAT	2003/07/28 12:14
9	5	((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))) and (emi or "electromagnetic interference" or "electro\$agnetic interference")	USPAT	2003/07/28 12:19
20	0	("(dslandsurgeandprotect\$4andmodemandinterface	USPAT	2003/07/28 13:29
21	0	(dsl and surge and protect\$4 and modem and interface).ab.	USPAT	2003/07/28 13:29
22	0	(dsl\$ and surge and protect\$4 and modem and interface).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:30
23	3	(dsl\$ and protect\$4 and modem and interface).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:30
24	2	(adsl and protect\$4 and modem and interface).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:30
25	0	(adsl and protect\$4 and modem and interface and transient).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:31
26	1	(protect\$4 and modem and interface and transient).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:38
27	5	((dsl\$ and protect\$4 and modem and interface).ab.) or ((adsl and protect\$4 and modem and interface).ab.) or ((protect\$4 and modem and interface and transient).ab.)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:31
28	4	(protect\$4 and modem and interface and surge).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:38
30	74	(protect\$4 and modem and surge).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:52
31	12	((protect\$4 and modem and surge).ab.) and modem.ti.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:48

33	125	((379/27.05).CCLS.) or (((379/412).CCLS.) and "diode bridge") and (((379/412).CCLS.) and surge)) or (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge)) and emi) or (((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))) and (emi or "electromagnetic interference" or "electro\$agnetic interference")) or ((dsl\$ and protect\$4 and modem and interface).ab.) or ((adsl and protect\$4 and modem and interface).ab.) or ((protect\$4 and modem and interface and transient).ab.)) or ((protect\$4 and modem and surge).ab.)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:53
34	15565	(data and access and (arrangement interface)).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:01
35	0	((data and access and (arrangement interface)).ab.) and (modem and emi and protection).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:58
36	10	((data and access and (arrangement interface)).ab.) and (modem and protection).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:58
37	911	("data access" and (arrangement interface)).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:02
38	143	("line access" and (arrangement interface)).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:04
39	1054	((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:04
43	5	((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and (protection and (surge transient)).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:06
44	18	(((((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and protection and (surge transient)) or (((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and (protection and (surge transient)).ab.)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:05

45	16	((((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and protection and (surge transient)) or (((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and (protection and (surge transient)).ab.)) not (((379/27.05).CCLS.) or (((379/412).CCLS.) and "diode bridge") and (((379/412).CCLS.) and surge)) or (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge)) and emi) or (((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))) and (emi or "electromagnetic interference" or "electro\$magnetic interference")) or (((dsl\$ and protect\$4 and modem and interface).ab.) or ((adsl and protect\$4 and modem and interface).ab.) or ((protect\$4 and modem and interface and transient).ab.)) or ((protect\$4 and modem and surge).ab.))	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:06
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1	23	(379/27.05).CCLS.	USPAT	2003/07/28 11:32
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6	165	((379/412).CCLS.) and "diode bridge") or ((379/412).CCLS.) and surge)	USPAT	2003/07/28 11:54
7	6	((379/412).CCLS.) and "diode bridge") or ((379/412).CCLS.) and surge)) and emi	USPAT	2003/07/28 12:14
8	200	((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))	USPAT	2003/07/28 12:14
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23	3	(dsl\$ and protect\$4 and modem and interface).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:30
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26	1	(protect\$4 and modem and interface and transient).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:38
27	5	((dsl\$ and protect\$4 and modem and interface).ab.) or ((adsl and protect\$4 and modem and interface).ab.) or ((protect\$4 and modem and interface and transient).ab.)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:31
28	4	(protect\$4 and modem and interface and surge).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:38
30	74	(protect\$4 and modem and surge).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:52
31	12	((protect\$4 and modem and surge).ab.) and modem.ti.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:48
33	125	((379/27.05).CCLS.) or (((379/412).CCLS.) and "diode bridge") and (((379/412).CCLS.) and surge)) or (((379/412).CCLS.) and "diode bridge") or ((379/412).CCLS.) and surge)) and emi) or (((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))) and (emi or "electromagnetic interference" or "electro\$agnetic interference")) or ((dsl\$ and protect\$4 and modem and interface).ab.) or ((adsl and protect\$4 and modem and interface).ab.) or ((protect\$4 and modem and interface and transient).ab.) or ((protect\$4 and modem and surge).ab.)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:53

34	15565	(data and access and (arrangement interface)).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:01
36	10	((data and access and (arrangement interface)).ab.) and (modem and protection).ab.	USPÄT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 13:58
37	911	("data access" and (arrangement interface)).ab.	USPÄT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:02
38	143	("line access" and (arrangement interface)).ab.	USPÄT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 15:17
39	1054	((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)	USPÄT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:04
43	5	((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and (protection and (surge transient)).ab.	USPÄT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:06
44	18	(((((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and protection and (surge transient)) or (((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and (protection and (surge transient)).ab.)	USPÄT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:05
45	16	(((((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and protection and (surge transient)) or (((("data access" and (arrangement interface)).ab.) or (("line access" and (arrangement interface)).ab.)) and (protection and (surge transient)).ab.)) not (((379/27.05).CCLS.) or (((379/412).CCLS.) and "diode bridge") and (((379/412).CCLS.) and surge)) or (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge)) and emi) or (((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))) and (emi or "electromagnetic interference" or "electromagnetic interference")) or ((dsl\$ and protect\$4 and modem and interface).ab.) or ((adsl and protect\$4 and modem and interface).ab.) or ((protect\$4 and modem and interface and transient).ab.)) or ((protect\$4 and modem and surge).ab.))	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 14:06
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51	2	((US-6411680-\$ or US-6282271-\$ or US-6212258-\$ or US-6563926-\$ or US-5146384-\$ or US-4941063-\$ or US-5642416-\$ or US-5369666-\$ or US-6351530-\$).did.) and emi	USPAT	2003/07/28 14:57

52	163	("data access arrangement").ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 15:18
53	161	((("data access arrangement").ab.) not (((379/27.05).CCLS.) or (((379/412).CCLS.) and "diode bridge") and (((379/412).CCLS.) and surge)) or (((((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge)) and emi) or (((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))) and (emi or "electromagnetic interference" or "electro\$magnetic interference")) or (((dsl\$ and protect\$4 and modem and interface).ab.) or ((adsl and protect\$4 and modem and interface).ab.) or ((protect\$4 and modem and interface and transient).ab.) or ((protect\$4 and modem and surge).ab.)) 1 (((("data access arrangement").ab.) not (((379/27.05).CCLS.) or (((379/412).CCLS.) and "diode bridge") and (((379/412).CCLS.) and surge)) or (((((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge)) and emi) or (((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))) and (emi or "electromagnetic interference" or "electro\$magnetic interference")) or (((dsl\$ and protect\$4 and modem and interface).ab.) or ((adsl and protect\$4 and modem and interface).ab.) or ((protect\$4 and modem and interface and transient).ab.) or ((protect\$4 and modem and surge).ab.))) and chassis 14 (capacitor with (EMI or electromagnetic) with "chassis ground")	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 15:19
57	1	1 (((("data access arrangement").ab.) not (((379/27.05).CCLS.) or (((379/412).CCLS.) and "diode bridge") and (((379/412).CCLS.) and surge)) or (((((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge)) and emi) or (((379/412).CCLS.) not (((379/412).CCLS.) and "diode bridge") or (((379/412).CCLS.) and surge))) and (emi or "electromagnetic interference" or "electro\$magnetic interference")) or (((dsl\$ and protect\$4 and modem and interface).ab.) or ((adsl and protect\$4 and modem and interface).ab.) or ((protect\$4 and modem and interface and transient).ab.) or ((protect\$4 and modem and surge).ab.))) and chassis 14 (capacitor with (EMI or electromagnetic) with "chassis ground")	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 15:25
58	14	14 (capacitor with (EMI or electromagnetic) with "chassis ground")	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 15:34
61	56	56 (modem and (chassis chasis)).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 15:35
62	1	1 ((modem and (chassis chasis)).ab.) and ground.ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 15:57
76	2	2 (emi and capacitor and ground and modem).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 15:59
78	16	16 (capacitor and ground and modem).ab.	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:01
81	64	64 "diode bridge" same capacitor same filter same (emi electromagnetic electro\$magnetic)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:14
84	0	0 (emi esd electrostatic electromagnetic) with "diode bridge" with (couple decouple) with filter	USPAT	2003/07/28 16:29
85	5430	5430 "diode bridge"	USPAT	2003/07/28 16:29
86	1	1 ("0000379").PN.	USPAT	2003/07/28 16:35
87	42845	42845 ("379").CLAS.	USPAT	2003/07/28 16:29

91	634	((("379").CLAS.) and "diode bridge"	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:30
92	292	((("379").CLAS.) and "diode bridge") and ((coupl\$4 decoupl\$4) with capacitor)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:35
93	34	((("379").CLAS.) and "diode bridge") and ((coupl\$4 decoupl\$4) with capacitor)) and (emi esd electrostatic electromagnetic)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:46
97	100999	network same coupl\$3	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:50
98	10413	network adj coupl\$3	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:50
100	12302	(diode or (full\$wave)) adj bridge	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:53
101	10618	diode adj1 bridge	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:52
102	683	((("379").CLAS.) and ((diode or (full\$wave)) adj bridge)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:53
103	19	((("379").CLAS.) and ((diode or (full\$wave)) adj bridge)) and (network adj coupl\$3)	USPAT; US-PGPUB; EPO; JPO; DERWENT; IBM_TDB	2003/07/28 16:53



US006351530B1

(12) **United States Patent**
Rahamim et al.

(10) **Patent No.:** **US 6,351,530 B1**
(45) **Date of Patent:** ***Feb. 26, 2002**

(54) **MODEM HAVING A DIGITAL HIGH VOLTAGE ISOLATION BARRIER**

(75) Inventors: **Raphael Rahamim**, Orange; **Thomas Grey Beutler**, Tustin, both of CA (US)

(73) Assignee: **Conexant Systems, Inc.**, Newport Beach, CA (US)

(*) Notice: Subject to any disclaimer, the term of this patent is extended or adjusted under 35 U.S.C. 154(b) by 0 days.

This patent is subject to a terminal disclaimer.

(21) Appl. No.: **09/193,222**

(22) Filed: **Nov. 16, 1998**

(51) Int. Cl.⁷ **H04M 11/00; H04M 3/50; H03M 3/02; H04B 3/00; H03K 1/04**

(52) U.S. Cl. **379/399.01; 379/93.05; 379/93.06; 379/93.07; 379/93.08; 379/93.29; 341/143; 370/494; 375/257**

(58) Field of Search **379/93.29, 93.05-93.08, 379/399.01; 341/143; 370/494; 375/257**

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Primary Examiner—Forester W. Isen

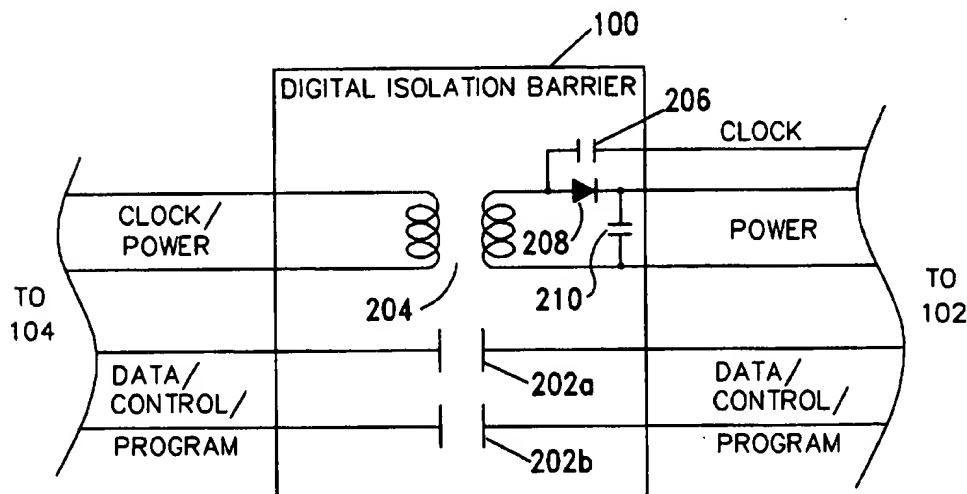
Assistant Examiner—Ramnandan Singh

(74) *Attorney, Agent, or Firm*—Akin, Gump. Strauss, Hauer & Feld, L.L.P.

(57) **ABSTRACT**

A modem utilizing a data access arrangement (DAA) having line side circuitry including a telephone network interface and system side circuitry including a host system interface. The line side circuitry and the system side circuitry are separated by a high voltage isolation barrier. In accordance with the invention, the high voltage isolation barrier and other DAA circuitry are configured such that information may be communicated between the system side circuitry and the line side circuitry in a digital format. In one embodiment of the invention, the high voltage isolation barrier comprises a single capacitor for communicating bidirectional digital data. In another embodiment of the invention, a pair of capacitors are provided in the high voltage isolation barrier, with the digital signals being driven in a differential manner. In yet another embodiment of the invention, a transformer is utilized for supplying clock signals and power across the high voltage isolation barrier, while a pair of capacitors (or a second transformer) is utilized to communicate bidirectional data.

19 Claims, 10 Drawing Sheets



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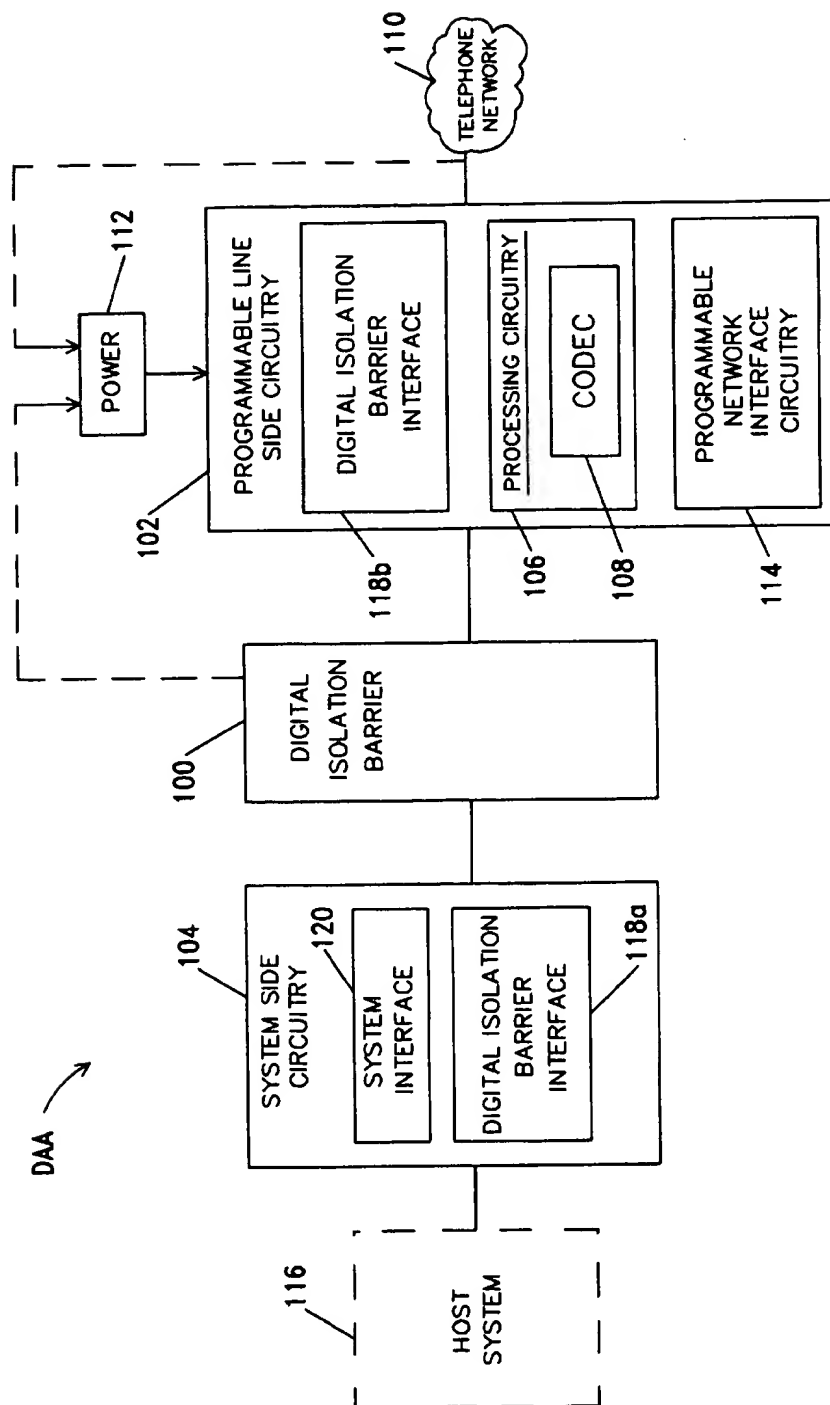


FIG.1

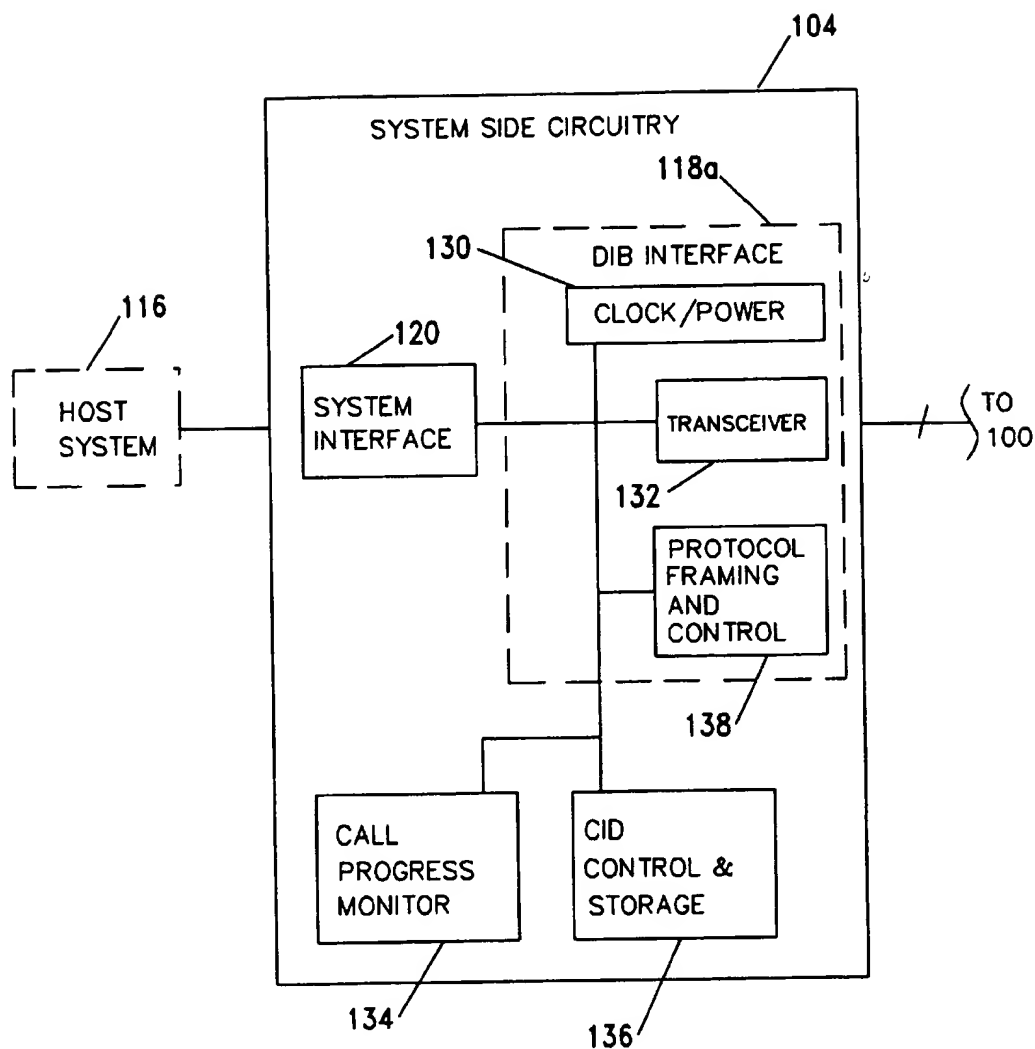


FIG. 2

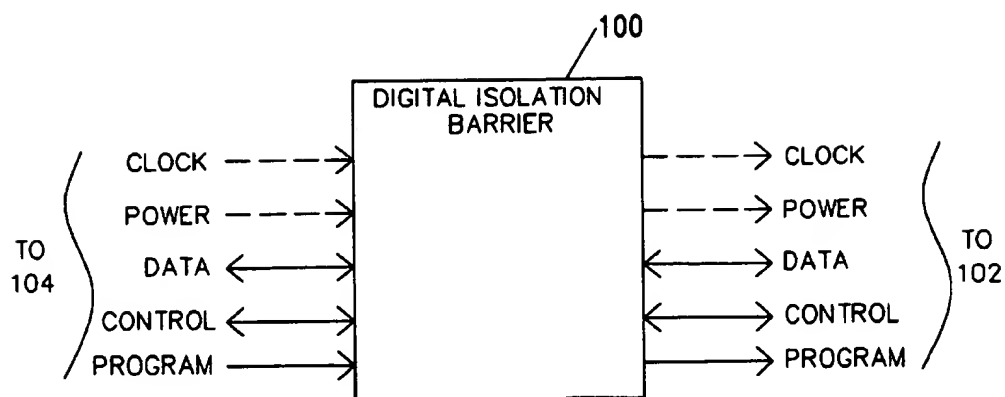


FIG. 3A

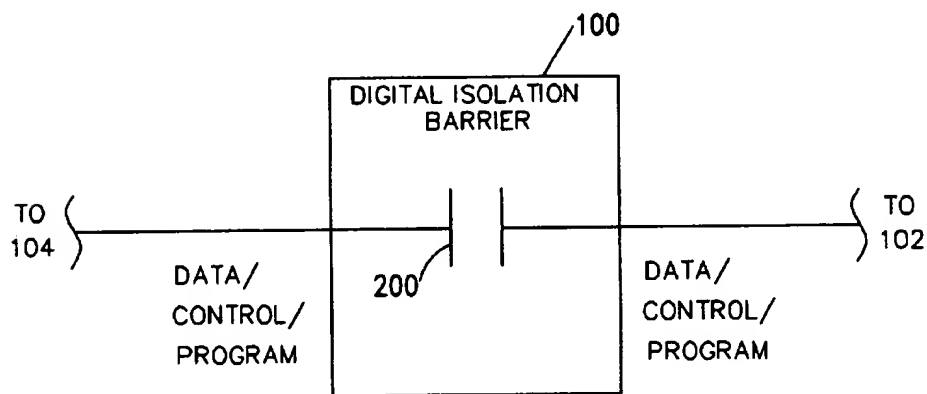


FIG. 3B

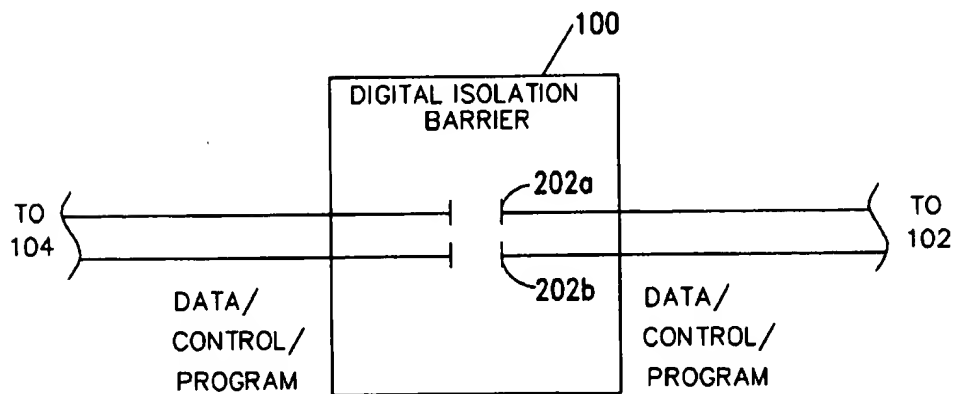


FIG. 3C

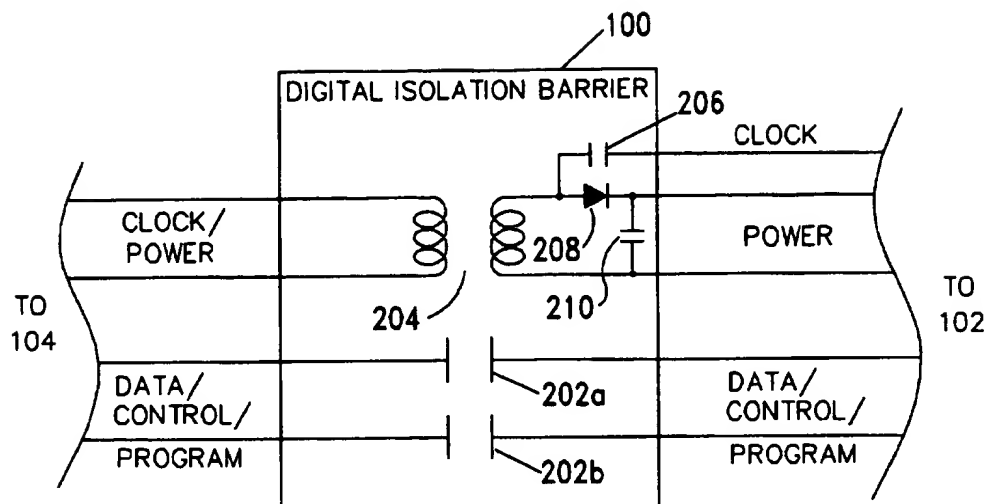


FIG. 3D

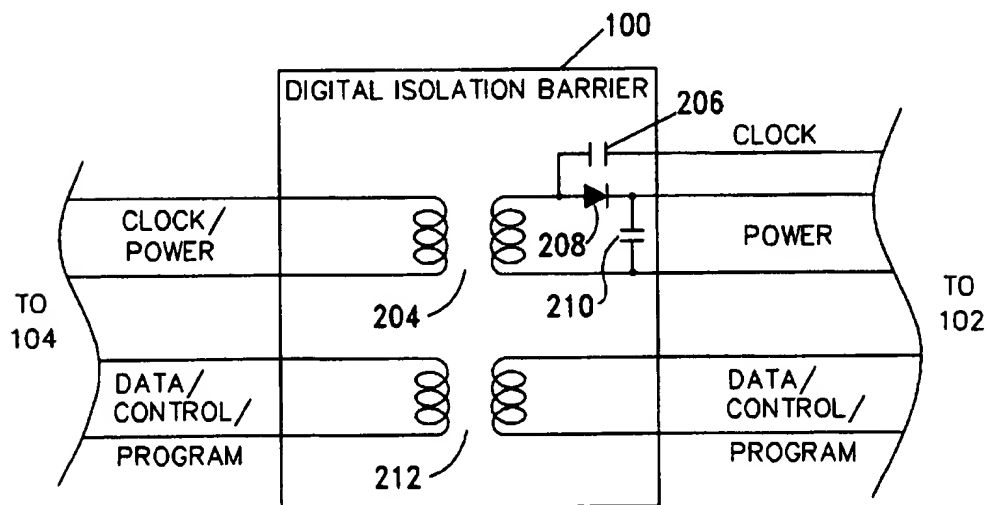


FIG. 3E

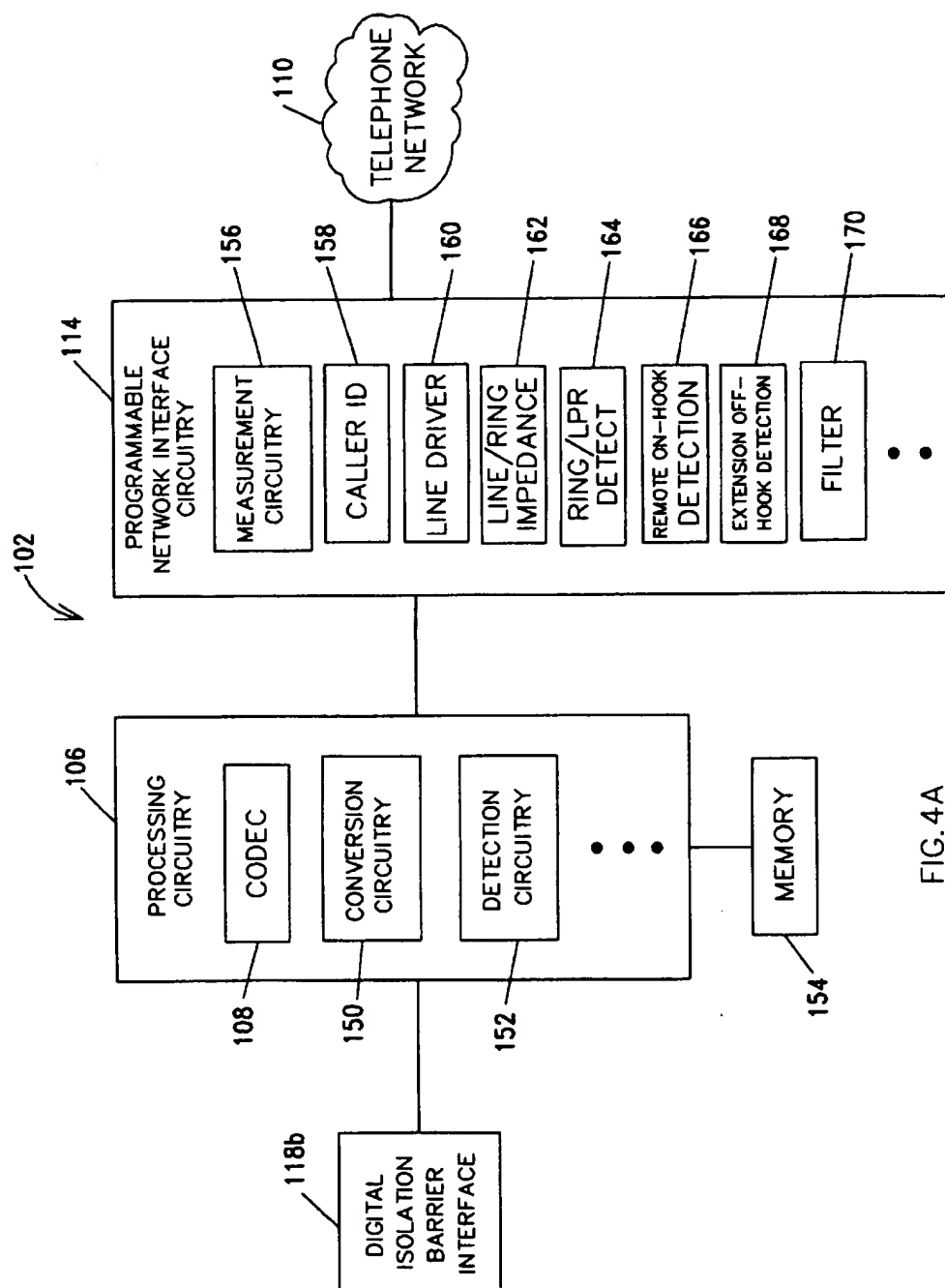


FIG. 4A

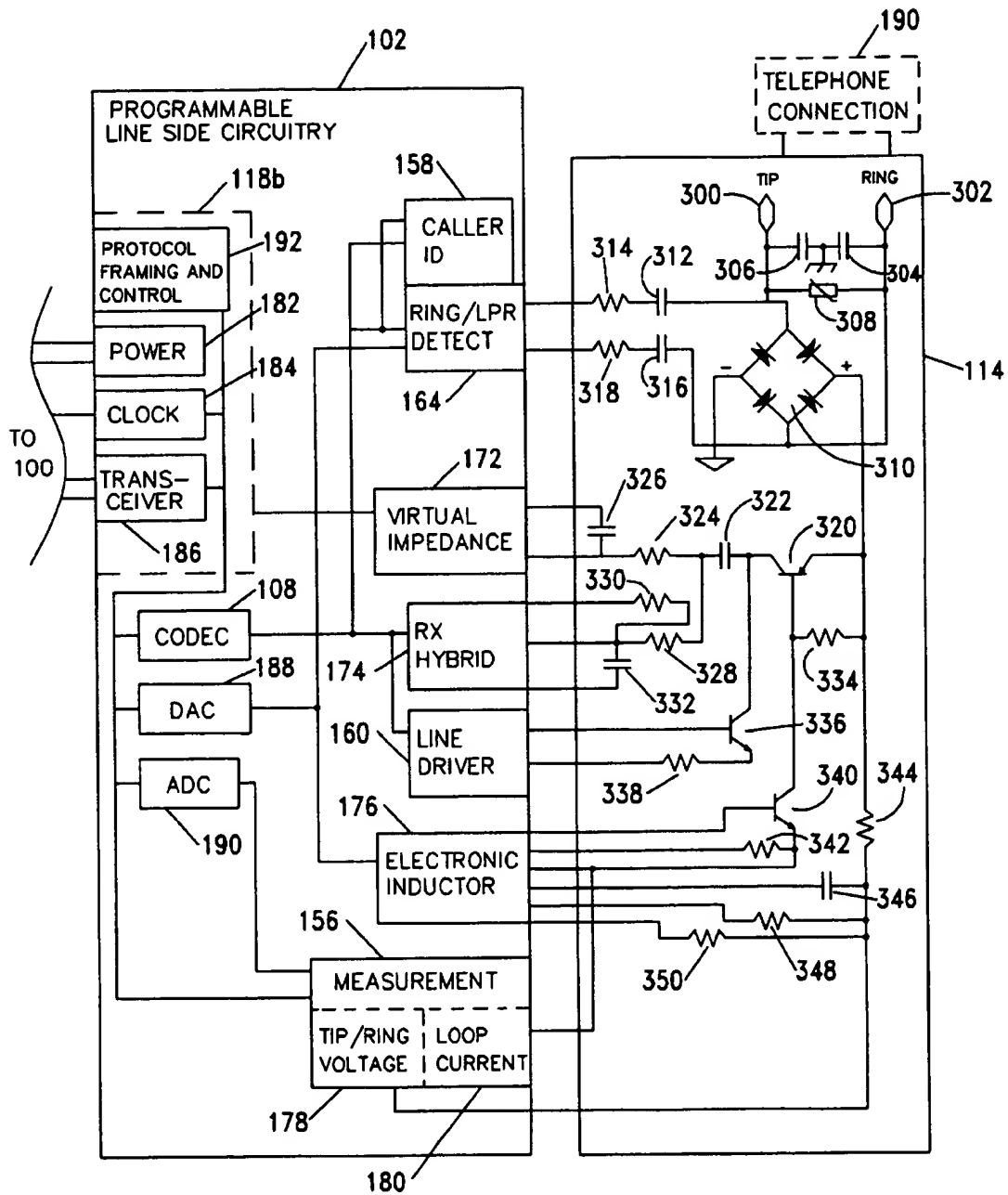


FIG. 4B

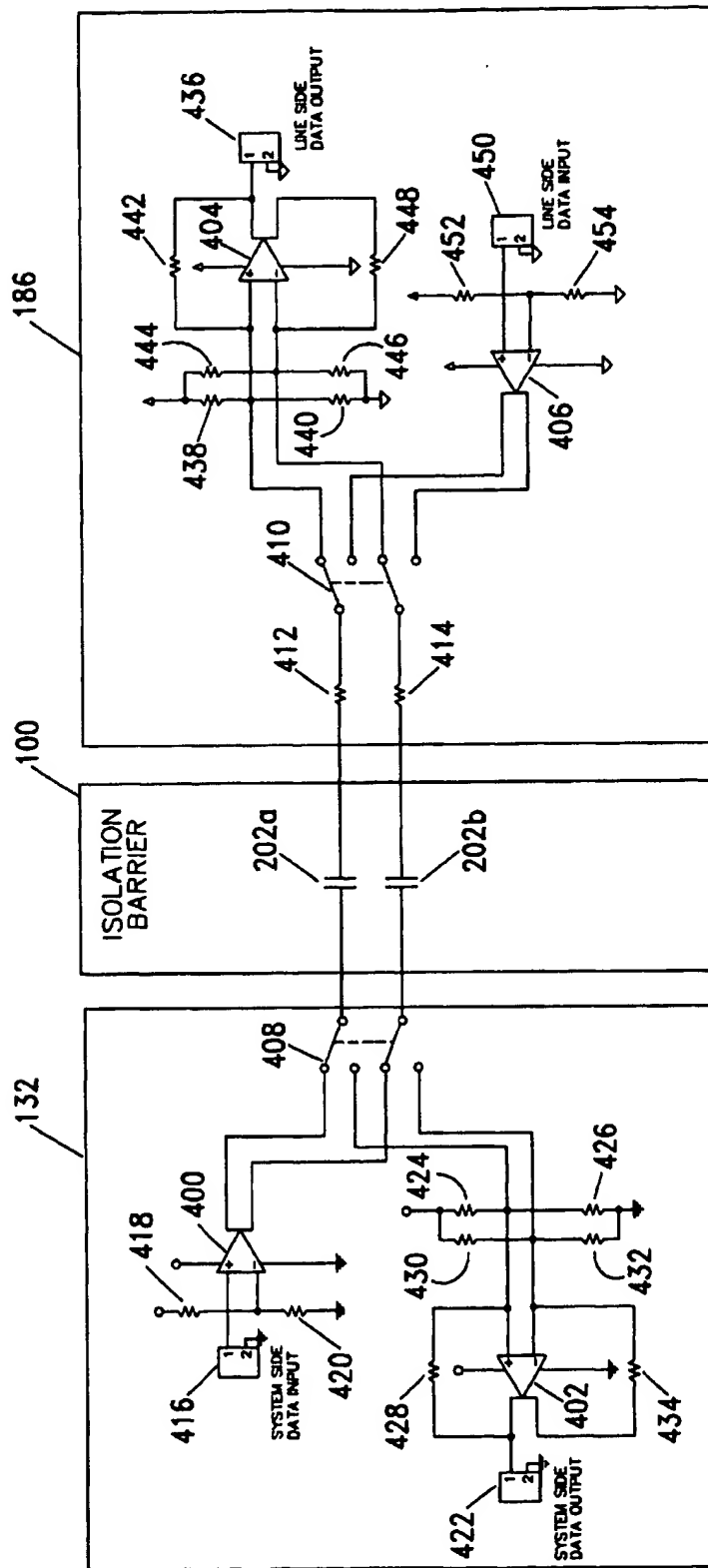


FIG. 5

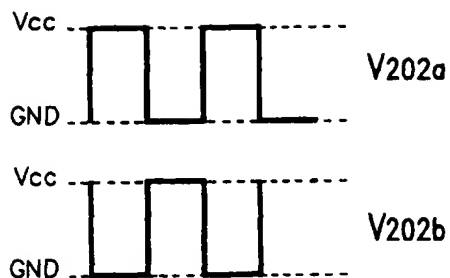


FIG.6

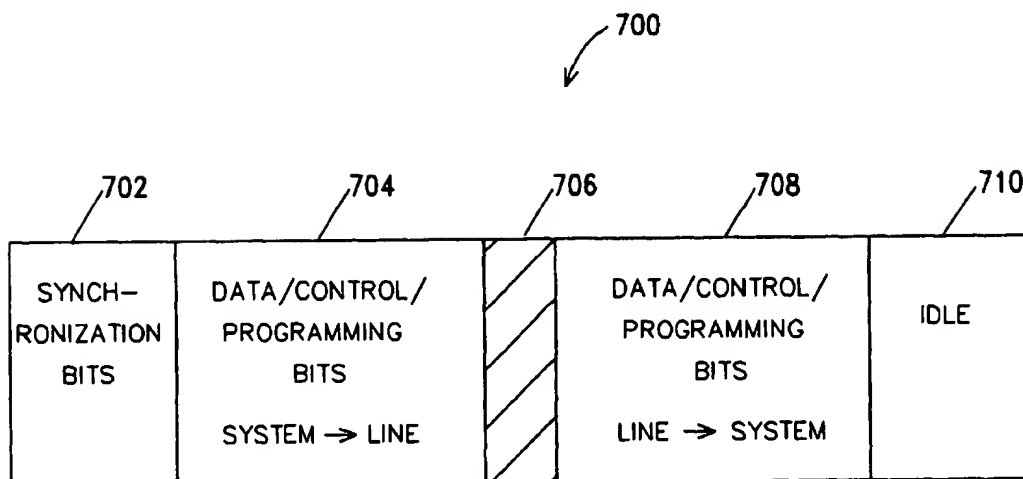


FIG.7

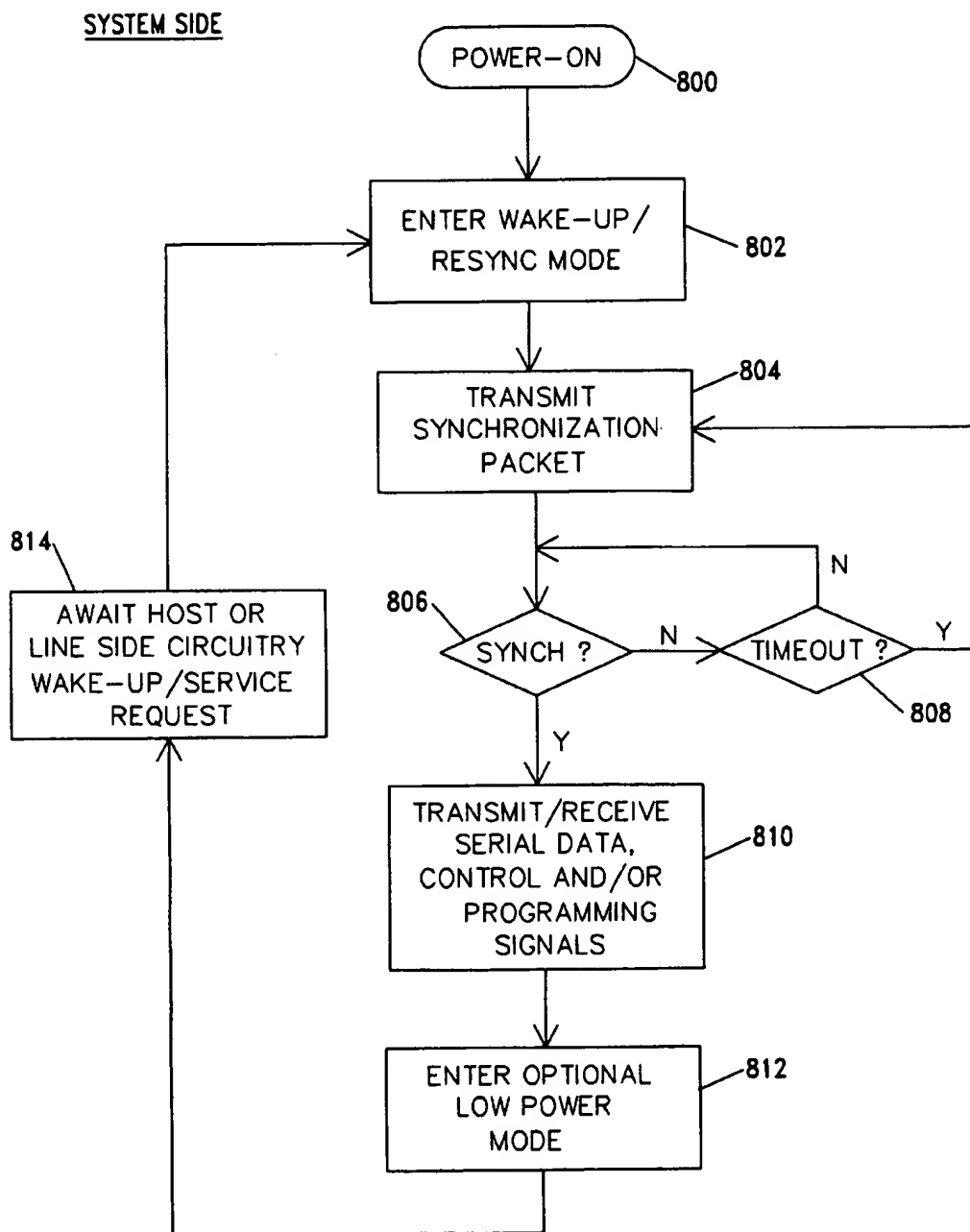


FIG. 8

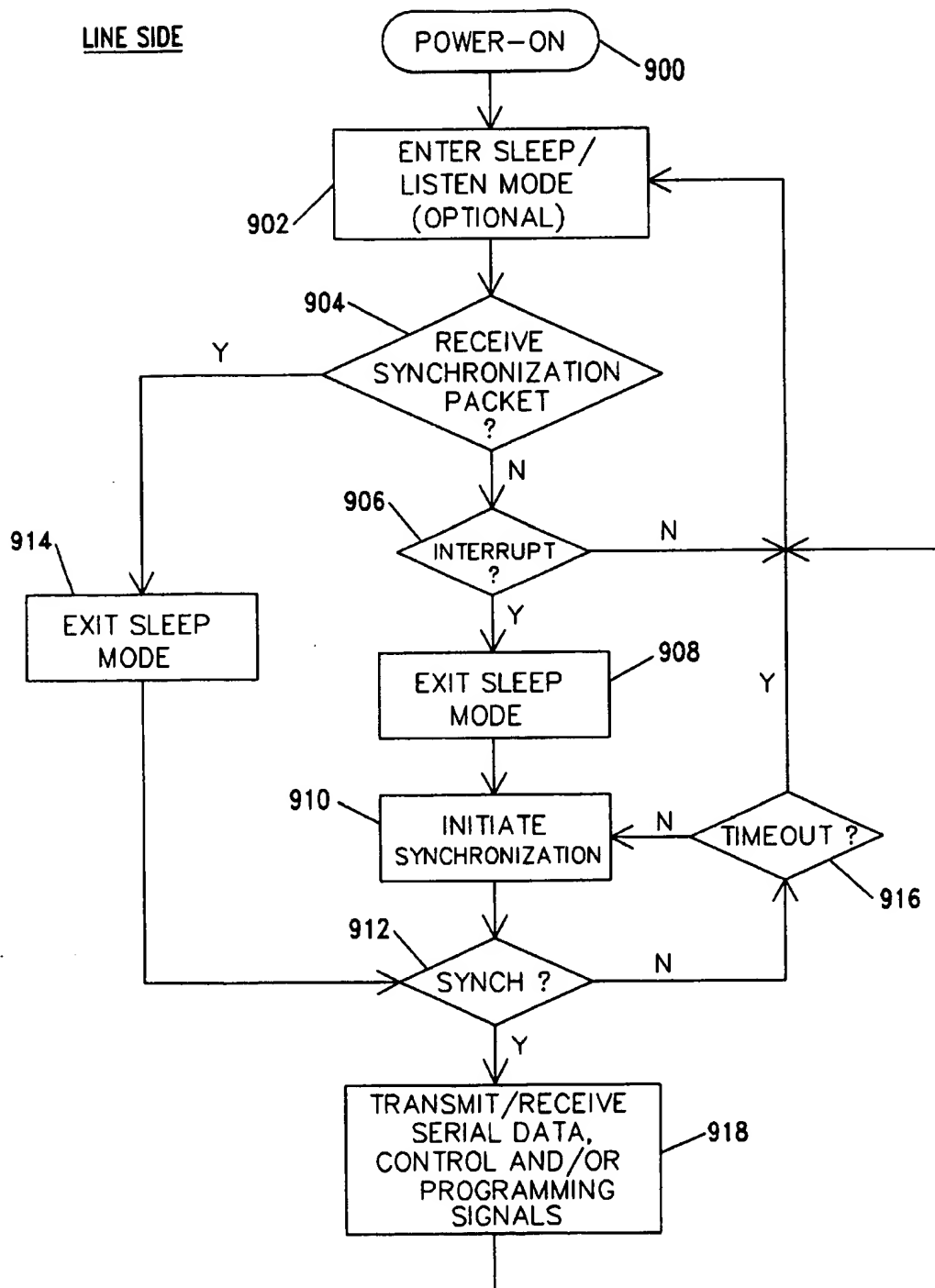


FIG. 9

MODEM HAVING A DIGITAL HIGH VOLTAGE ISOLATION BARRIER

INCORPORATIONS BY REFERENCE

The following commonly-assigned patent applications are hereby incorporated by reference in their entirety, including drawings and appendices, and are hereby made part of this application for all purposes:

- 1) U.S. patent application Ser. No. 09/161,209, filed Sep. 25, 1998;
- 2) U.S. patent application Ser. No. 09/088,629, filed Jun. 2, 1998;
- 3) U.S. patent application Ser. No. 09/074,896, filed May 8, 1998;
- 4) U.S. patent application Ser. No. 09/075,451, filed May 8, 1998; and
- 5) U.S. patent application Ser. No. 09/929,960, filed Sep. 15, 1997.

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BACKGROUND

1. Technical Field

The present invention relates generally to modems; and, more particularly, it relates to a data access arrangement having a high voltage isolation barrier configured to communicate information in a digital format.

2. Related Art

Regulatory agencies throughout the world have established standards and regulations for connecting subscriber equipment to telephone networks. These regulations are intended to prevent damage to the telephone network and mitigate interference with other equipment also connected to the network. The regulations, however, often present difficult design challenges.

For example, subscriber equipment or data communications equipment (DCE), such as a data modem, is generally required to provide for some form of electrical isolation to prevent voltage surges or transients originating from the subscriber equipment from having a deleterious effect on the telephone network. Electrical isolation also addresses potential problems associated with differences in operating voltages between a telephone line and the subscriber equipment. More particularly, telephone line voltages may vary widely across a given network, and often exceed the operating voltage of subscriber equipment. In the United States, 1,500 volt isolation is currently required. In other countries, the prescribed isolation may reach 3,000–4,000 volts.

A number of techniques have been utilized to provide the requisite level of electrical isolation. For example, isolation transformers are often employed to magnetically couple signals between a two-wire telephone line and the analog front end of a modem or other circuit while maintaining an appropriate level of electrical isolation. The isolation transformer functions to block potentially harmful DC components, thereby protecting both sides of the data connection.

The isolation transformer is typically part of what is referred to in the modem arts as a data access arrangement (DAA). The term DAA generally refers to circuitry, which provides an interface between a public telephone network originating in a central office (CO) and a digital data bus of a host system or data terminal equipment (DTE). The DAA electrically isolates a modem or similar device from a phone line to control emissions of electromagnetic interference/radio frequency interference (EMI/RFI). In addition to electrical isolation, the DAA often develops a number of signals (e.g., a ring signal) for provision to subscriber equipment. The DAA may receive signals from the phone line through a telephone jack, such as a RJ11C connection as used for standard telephones.

Typically, a number of circuits must derive information from the telephone line, and isolation is often required for each signal communicated to and from the host system. Such circuits may include: transmit and receive circuitry; ring signal detection circuitry; circuitry for switching between voice and data transmissions; circuits for dialing telephone numbers; line current detection circuitry; circuitry for indicating that the equipment is coupled to a functional telephone line; and line disconnection detection circuitry. Conventional DAA designs utilize separate line side circuits and separate signal paths across a high voltage isolation barrier for each function of the DAA.

Modems function to convert analog signals from the telephone network to a digital format that can be used by the host system. Most countries have specific regulatory requirements governing off-hook voltage and loop current, ring detect threshold levels, and line interface impedances that must be taken into account by devices such as modems. Such electrical characteristics of a DAA are often difficult to control, due in part to the fact that the circuits which determine these characteristics are located on the line side of the high voltage isolation barrier.

Further, it is difficult to configure a DAA to satisfy the regulatory requirements of more than one country. Conventional non-programmable DAA designs are only suitable for a single country or a group of countries with similar requirements.

While the isolation transformer of a DAA protects the electronic components of a modem, it often introduces distortion and consumes a relatively large amount of space. In today's world of ever-shrinking electronics, the bulk of the isolation transformer may govern the physical dimensions of the modem itself and impose other unwanted constraints on cost sensitive modem circuitry.

One method for reducing the size of the isolation transformer in a DAA involves coupling certain telephone line signals (e.g., incoming ringing signals) to modem circuitry while utilizing a separate signal path to couple data signals via a capacitively coupled isolation transformer. Although enabling the use of smaller and lighter isolation transformers, this configuration may result in excessive distortion.

Some modem configurations have eliminated the isolation transformer altogether via the use of analog electro-optical isolators. These devices employ an emitter, such as a light emitting diode, and a corresponding photo-detector circuit. This type of isolation, however, may suffer from distortion, cost and complexity issues.

Still other configurations have used an isolation transformer in the main signal path and optical isolators or relays in the ring detection and off-hook driving circuitry. Capacitors have also been utilized to differentially couple analog

transmit and receive channels across an isolation barrier. Thermal and resistive isolation techniques have also been employed, but are typically complex and expensive to manufacture.

The requirement of passing analog audio signals across the high voltage isolation barrier for provision to a coder/decoder (CODEC) and other DAA circuitry hampers efforts to decrease the size and cost of the barrier due to the foregoing design constraints. Further, each signal path across the barrier adds to size and expense of the high voltage isolation barrier.

SUMMARY OF THE INVENTION

Briefly, a modem according to the present invention utilizes a DAA having line side circuitry including a telephone network interface and system side circuitry including a host system interface. The line side circuitry and the system side circuitry are separated by a high voltage isolation barrier. In accordance with the invention, the high voltage isolation barrier and other DAA circuitry are configured such that information may be communicated between the system side circuitry and the line side circuitry in a digital format.

In one embodiment of the invention, the high voltage isolation barrier comprises a single capacitor for communicating bidirectional digital data. In another embodiment of the invention, a pair of capacitors are provided in the high voltage isolation barrier, with the digital signals being driven in a differential manner. In yet another embodiment of the invention, a transformer is utilized for supplying clock signals and power across the high voltage isolation barrier, while a pair of capacitors (or a second transformer) is utilized to communicate bidirectional data. A high voltage isolation barrier according to the invention thus provides an inexpensive and physically compact way to pass digital signals in both directions utilizing as few as one capacitor or one transformer.

BRIEF DESCRIPTION OF THE DRAWINGS

A better understanding of the present invention can be obtained when the following detailed description of an exemplary embodiment is considered in conjunction with the following drawings, in which:

FIG. 1 is a drawing of an exemplary data access arrangement implemented in accordance with the present invention;

FIG. 2 is a drawing illustrating an exemplary embodiment of the system side circuitry of the data access arrangement of FIG. 1;

FIGS. 3A-3E are drawings providing alternate embodiments of a digital isolation barrier according to the present invention;

FIGS. 4A and 4B are drawings providing exemplary details of the line side circuitry of the data access arrangement of FIG. 1;

FIG. 5 is a drawing of exemplary transceiver circuitry according to the present invention for communicating a serial datastream across the digital isolation barrier of FIG. 1;

FIG. 6 is a voltage waveform drawing illustrating differential communications across the digital isolation barrier of FIG. 5;

FIG. 7 is an illustration of an exemplary serial protocol according to the present invention for communicating information across the digital isolation barrier of FIG. 1;

FIG. 8 is a flow chart depicting exemplary serial communication steps, performed by the system side circuitry of FIG. 1, according to the present invention; and

FIG. 9 is a flow chart depicting exemplary serial communication steps, performed by the line side circuitry of FIG. 1, in accordance with the present invention.

DETAILED DESCRIPTION

FIG. 1 is a schematic block diagram illustrating an exemplary DAA in accordance with the present invention. The DAA of the disclosed embodiment of the invention includes a digital isolation barrier 100 for communicatively coupling programmable line side circuitry 102 to system side circuitry 104. The digital isolation barrier 100, in conjunction with programmable features of the line side circuitry 102 which interface with a telephone network 110, provide the necessary level of electrical isolation between the line side circuitry 102 and the corresponding system side circuitry 104. The digital isolation barrier 100 is designed to be configurable to comply with both U.S. and International requirements for isolation.

The system side circuitry 104 includes a system interface 120 and a digital isolation barrier interface 118a. The system interface 120 coordinates communications with the host system circuitry 116, while the digital isolation barrier interface 118a establishes communications with the digital isolation barrier 100. Data, control and programming signals are all communicated across the digital isolation barrier 100. The bidirectional communication from the system side circuitry 104 and the line side circuitry 102 is accomplished via a digital protocol, examples of which are described below in conjunction with FIGS. 7-9 and Appendix A, which is hereby incorporated by reference and made part of this specification as if set forth in its entirety.

The programmable line side circuitry 102 includes a digital isolation barrier interface 118b corresponding to the digital isolation barrier interface 118a of the system side circuitry 104. The programmable line side circuitry 102 also includes processing circuitry 106 and programmable network interface circuitry 114. Many functions are performed by the programmable network interface circuitry 114, including measuring and establishing electrical parameters that are reflective of the condition of the lines of the telephone network 110.

The processing circuitry 106 of FIG. 1 includes a coder/decoder (CODEC) 108. The CODEC 108 functions to encode the analog signal on the lines of the telephone network 110 into a digital format, and also provides decoded digital signals for analog transmission over the telephone network 110. In a conventional DAA, a CODEC is disposed on the system side of a high voltage isolation barrier. In accordance with the present invention, however, the CODEC 108 is advantageously included on the line side of a digital isolation barrier 100 to facilitate communications with the line side circuitry 102. In addition, placement of the CODEC 108 and other circuitry/functions on the line side reduces the number of signals communicated across the digital isolation barrier 100 and facilitates programmability of the network interface circuitry 114.

Programmability of the network interface circuitry 114 may be achieved in a variety of ways. For example, if the host system circuitry 116 desires to program a particular feature of the line side circuitry 102 (e.g., vary line/ring impedance), a command or programming signal is communicated to the system side 104. The command or programming signal may then be reconfigured for transmission to the line side circuitry 102 in a digital manner via the digital isolation barrier 100. Alternatively, the command or programming signal may originate in the system side circuitry 104, or be directed

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towards the system side circuitry 104 by the line side circuitry 102. Command or programming signals may be multiplexed and serialized for transmission across the digital isolation barrier 100, thereby reducing the complexity and expense of the digital isolation barrier. Data signals may also be combined with the command or programming signals, further simplifying the digital isolation barrier 100.

The line side circuitry 102 of the disclosed embodiment of the invention operates with a "floating" ground reference, and can tolerate high voltage inputs for compatibility with the telephone network 110 and typical surge requirements. The system side circuitry 104 of the disclosed embodiment operates with a fixed digital ground and utilizes standard CMOS logic levels. The system side circuitry 104 shares a common ground and power supply with the host system circuitry 116. The programmable line side circuitry 102 of the disclosed embodiment receives power from either the digital isolation barrier 100 or the telephone network 110 via a power connection 112.

A DAA in accordance with the invention can be utilized with any product that interfaces a telephone network 110 connection to any digital signal processor technology, or any processor of host system circuitry 116 that performs analog modem modulations. Examples include, but are not limited to, data modems, computers, web browsers, set top boxes, fax machines, cordless telephones and telephone answering machines. In addition, many different interfaces with the telephone network 110 and/or other transmission media are contemplated, such that the DAA may be configured to be compatible with whichever means is utilized.

FIG. 2 is a drawing illustrating an exemplary embodiment of the system side circuitry of the data access arrangement of FIG. 1. The digital isolation barrier interface 118a of the disclosed embodiment includes clock/power driver circuitry 130, as well as protocol framing and control circuitry 138 and a transceiver 132, which coordinate bidirectional transfer of data, control and programming signals across the digital isolation barrier 100.

The clock and power driver circuitry 130 is responsible for transferring power and clock signals across the digital isolation barrier 100 to the line side circuitry 102 via the digital isolation barrier 100. The clock and power driver circuitry 130 is programmable by the system side circuitry 102 to include a number of power states, including: an off-hook, high power mode in which line side circuitry 102 is powered by the system side circuitry 104; an off-hook, low power mode in which the line side circuitry 102 is powered by the telephone network 110 and/or the system side circuitry 104; and on-hook, low power mode in which the line side circuitry 102 is waiting for a ring or a caller ID signal; and an on-hook, disabled state in which the line side circuitry 102 is not receiving power. The clock and power driver circuitry provides several different drive current levels as needed for different operating/power consumption modes of the line side circuitry 102. As noted, certain embodiments or power modes of the line side circuitry 102 may not require power from the clock and power driver circuitry 130.

The digital isolation barrier interface 118a also includes a protocol framing and control circuit 138, which functions to organize the data transmitted by the transceiver 132. The protocol framing control circuit 138 also deconstructs signals received by the transceiver 132 from the line side circuitry 102.

Inputs to the system interface circuit 120 include inputs for off-hook signal(s), caller ID number information, inter-

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national control signals, and reserved signals for upgrades. Outputs of the system interface circuit 120 include but are not limited to a line side off-hook signal, an extension off-hook signal, a remote on-hook signal, a digital PBX signal, a ring indication signal, and a wake signal. General-purpose I/O functions are also provided.

Numerous alternative implementations for the communication lines between the host system circuitry and the system interface circuit 120 are contemplated. For example, the system interface circuit 120 may be configured to interface directly with a controllerless host architecture. A high-speed serial data interface or a parallel data interface with various I/O lines for modem control and DAA status may also be used. Likewise, the call progress monitor 134 and the CID control and storage circuitry 136 may be included in the host system circuitry 116 or in the line side circuitry 102, and the transceiver circuitry 132 and 186 may provide for serial communications, parallel communications, or a combination thereof.

The system side circuitry 108 also includes a call progress monitor 134 and a caller ID (CID) control and storage circuit 136. The call progress monitor 134 is configured to analyze raw signal samples from the CODEC 108 and drive a buzzer or speaker (not shown). The call progress monitor 134 of the disclosed embodiment is also programmable to provide a variety of audio levels.

The CID control and storage circuit 136 is preferably configurable to support all known worldwide caller ID schemes. This includes, but is not limited to, the United States and North America, Japan, Western Europe (including the United Kingdom and France). Accordingly, the CID control and storage circuit 136 supports both caller ID information occurring between rings and after a tip/ring reversal (United Kingdom). The CID control and storage circuit 136 also provides memory (not separately illustrated) for storing a digital representation of caller ID information received from the digital interface barrier 100. Caller ID data is decoded before storage in the memory, although storage of raw information is acceptable. The CID control and storage circuitry 136 of the disclosed embodiment is programmable to be disabled by the host system circuitry 116 or other portions of the DAA.

FIGS. 3A-3E depict exemplary alternate embodiments of a digital isolation barrier 100 implemented in accordance with the present invention. Referring first to FIG. 3A, a number of signals may be communicated between the line side circuitry 102 and the system side circuitry 104. As noted above, a clock signal may be passed from the system side circuitry 104 to the line side circuitry 102 in order to facilitate synchronization of serial communications. In addition, the line side circuitry 102 may be powered completely or in part by a power signal communicated across the digital isolation barrier 100. Further, serial data, control and/or program signals are also communicated across the digital isolation barrier 100. As discussed immediately below, a variety of electrical configurations for transferring these signals across the digital isolation barrier are possible.

FIG. 3B depicts an embodiment of the digital isolation barrier 100 in which the serial datastream is communicated across a signal path employing a single capacitor 200. In this embodiment, the transceiver circuitry 132 and 186 of the system side circuitry 104 and the line side circuitry 102, respectively, are configured to communicate a single-ended pulse train across the capacitor 200.

FIG. 3C depicts an embodiment of the digital isolation barrier 100 in which the single capacitor configuration is

replaced by a differential configuration involving capacitors 202a and 202b. In this embodiment, the serial datastream consisting of data, control and/or programming signals is organized in the same manner as if the interface of FIG. 3B were utilized. However, the transceiver circuitry 132 and 186 is configured for differential communications when utilized with the digital isolation barrier of FIG. 3C. One example of such a configuration is discussed below in conjunction with FIG. 5.

FIG. 3D illustrates another contemplated embodiment for the digital isolation barrier 100. In this embodiment, a transformer 204 is added to the circuitry of FIG. 3C to communicate clock and power signals from the system side circuitry 104 to the line side circuitry 102. More specifically, the primary side of the transformer 204 is driven by the system side circuitry 104 such that clock and power signals of sufficient strength can be derived from the secondary side of the transformer 204. The clock signal, if provided, is coupled to the line side circuitry 102 via a relatively small value capacitor 206. The power connections of the line side circuitry 102 are coupled to the secondary side of the transformer 204 via a half wave rectifier comprising a voltage regulating diode 208 and a charge storage capacitor 210. The capacitor 210 is provided across the power and ground connections of the line side circuitry 102 to provide a stable power supply voltage.

Although the disclosed embodiment of FIG. 3D employs a half wave rectifier, a full wave rectifier or a bridge rectifier could also be utilized. In another contemplated embodiment, clock and power signals are communicated across the digital interface barrier 100 via a separate pair of capacitors (not shown).

FIG. 3E illustrates another alternate embodiment of the digital isolation barrier 100. In this embodiment, an isolation transformer 212 replaces the isolation capacitors 202a and 202b. Data, control and programming signals are communicated between the system side circuitry 104 and the line side circuitry 102 utilizing the same serial data protocol of the other embodiments. Although not separately illustrated, other types of circuitry (such as opto-couplers and thermal relay circuitry) may be used to effect a digital isolation barrier 100 in accordance with the present invention.

FIG. 4A is a drawing providing exemplary details of an embodiment of the line side circuitry of the data access arrangement of FIG. 1. As described above, the line side circuitry 102 is isolated from the rest of the DAA by the digital isolation barrier interface 118b and the digital isolation barrier 100 in order to comply with applicable regulatory requirements.

The line side circuitry 102 of FIG. 4A includes processing circuitry 106 and programmable network interface circuitry 114. The processing circuitry 106 of the disclosed embodiment is comprised of a CODEC 108, conversion circuitry 150 and detection circuitry 152. A memory 154 is also provided for use by the processing circuitry 106. Various components of the processing circuitry 106 may be configurable by the system side circuitry 104, or pre-programmed by code stored in the memory 154. It is further contemplated that the memory 154 may store electrical specifications and configurations relating to the regulatory requirements of various countries.

The CODEC 108 of the disclosed embodiment of the invention is a 16 bit, 16 KHz a second order sigma-delta CODEC used for sampling analog signals on the telephone network 110, and to provide such signals to the telephone network 110. The conversion circuitry 150 includes an

analog-to-digital converter (ADC) and a digital-to-analog converter (DAC) for supporting various functionality of the programmable network interface circuitry 114. The detection circuitry 152 may serve a variety of functions, including monitoring of the programmable network interface circuitry 114 for significant changes in the status of the telephone network 110, as well as monitoring and execution of commands from the system side circuitry 104.

The programmable network interface circuitry 114 includes a wide variety of programmable functions. For example, programmable measurement circuitry 156 is provided with adjustable parameters for measuring tip/ring voltage and loop current conditions on the lines of the telephone network 110.

The caller ID circuit 158 receives and decodes caller identification information from the telephone network 110. To this end, it includes a relatively simple ADC and a demodulator complying with one or more standards (e.g., V.23/Bell 202, ETSI 300). It is also capable of transferring caller identification information across the digital isolation barrier 100 in a low power or D3cold state, and is programmable to provide caller ID information without a ring or line polarity reversal.

Signals are provided by the DAA to the telephone network 110 via line driver circuitry 160. The line driver circuitry 160 of the disclosed embodiment is programmable to drive signals having the electrical characteristics prescribed by the country in which the DAA is being used. Programmable line/ring impedance circuitry 162 is also provided to allow the DAA or host system circuitry 116 to program the electrical characteristics of the DAA as seen by the telephone network 110 to facilitate compliance with a variety of regulatory standards, including country-by-country ring loading. Values measured by the measurement circuitry 156 may be used in this process. In addition, the programmable line/ring impedance matching circuitry 162 of the disclosed embodiment includes support for metering filters.

The ring/line polarity reversal (LPR) detection circuitry 164 of the disclosed embodiment is likewise programmable to comply with both U.S. and international requirements. The ring/LPR detection circuitry 164 functions to provide ring and ring wake bit signals. In addition, the ring/LPR detection circuitry 164 is configurable to provide line current sensing information for use by remote on-hook detection circuitry 166, extension off-hook detection circuitry 168 and digital PBX functions.

Other contemplated components of the programmable network interface circuitry 114 include, for example: filtering circuitry 170, pulse dialing circuitry, hook switch circuitry, general purpose I/O lines, line current sensing for digital PBX detection, measurement circuitry for determining Central Office battery and loop DC resistance, line in use indicators, PABX digital line detection circuitry, and host controlled worldwide DC masks. Many of the disclosed features allow the host system circuitry 116 to easily ascertain the condition of the telephone network 110. The line side circuitry 102 further includes a hard coded key (or sequence of keys) that can be used by software executed by a microcontroller or by digital signal processing circuitry (not separately illustrated) to enable itself.

FIG. 4B is a drawing providing exemplary details of another embodiment of the line side circuitry of the data access arrangement of FIG. 1. The digital isolation barrier interface 118b of this embodiment includes a protocol framing and control circuit 192 that functions to organize the

data transmitted by the transceiver 186. The protocol framing circuit 192 also deconstructs signals received by the transceiver 186 from the system side circuitry 104. In addition, an optional power regulation circuit 182 is provided if the line side circuitry 102 receives power from the system side circuitry 104. Likewise, a clock circuit 184 is provided in the digital isolation barrier interface 118b to receive a signal from the system side circuitry 104 for use in generating clock signals for the logic of the programmable line side circuitry 102. Further details of the operation of an exemplary power regulation circuit 182 and an exemplary clock circuit 184 may be found in previously incorporated U.S. patent application Ser. No. 09/088,629, filed Jun. 2, 1998, and U.S. patent application Ser. No. 09/161,209, filed Sep. 25, 1998.

In addition to the CODEC 108, a DAC 188 and an ADC 190 are also provided. The DAC 188 and ADC 190 may operate as part of the CODEC 108, or may be separate circuits for use by other components of the line side circuitry 102. For example, the DAC 188 of the disclosed embodiment is utilized by a ring/LPR detection circuitry 164 and an electronic inductor 176. Similarly, the ADC 190 operates in conjunction with the measurement circuitry 156, which includes tip/ring voltage measurement circuit 178 and loop current measurement circuitry 180.

A hybrid circuit 174 is coupled to the CODEC 108 for performing two wire to four wire conversion functions and to provide incoming signals to the CODEC 108. A line driver circuit 160 is also coupled to the CODEC 108 and other analog circuitry of the programmable network interface 114. The line driver provides signals from the CODEC 108 to the tip 300 and ring 302 conductors of the telephone connection 190.

The analog circuitry of the programmable network interface 114 includes electromagnetic interference (EMI) suppression capacitors 306 and 304 coupled between the tip connection 300 and ring connection 302, respectively, of the telephone connection 190. In addition, a metal oxide varistor 308 is coupled between the tip connection 300 and ring connection 302 to provide lightning and surge protection. It is contemplated that the metal oxide varistor 308 could be replaced by a sidactor or similar circuit.

A full wave rectifier 310 is also coupled between the tip connection 300 and ring connection 302. As known to those skilled in the art, the full wave rectifier 310 ensures that the same polarity of DC signal is present at its "+" terminal regardless of the DC polarity of the tip and ring connections 300 and 302. In addition, a capacitor 312 and resistor 314 are coupled in series between the tip connection 300 and the ring/LPR detection circuitry 164. Similarly, a capacitor 316 and resistor 318 are coupled between the ring connection 302 and the ring/LPR detection circuitry 164. These connections provide differential inputs to the ring/LPR detect circuitry 164.

The emitter of a bipolar junction transistor 320 is coupled to the "+" terminal of the full wave bridge rectifier 310, while its collector is coupled to a capacitor 322 and a transistor 336. The transistor 320, in conjunction with a resistor 334 coupled between its emitter and base, functions to isolate the virtual impedance circuit 172 and the hybrid circuit 174 from the telephone connection 190 when in an on-hook condition. The virtual impedance circuit 172 is coupled to the capacitor 322 via a capacitor 326 and resistor 324, while the hybrid circuit 174 is coupled to the capacitor 322 via resistors 328 and 330 and a capacitor 332. In the disclosed embodiment, these resistors and capacitors pro-

vide signal gain/conditioning to allow the virtual impedance circuit 172 and hybrid circuit 174 to operate at a variety of tip/ring voltage levels. The transistor 320 and the resistor 334 are not required in certain contemplated applications.

The transistor 336 and resistor 338, which are coupled to the line driver circuit 160, allow the line side circuitry 102 to provide signals to the tip and ring connections 300 and 302 via the full wave bridge rectifier 310. More specifically, modulation of the base-collector voltage of the transistor 336 allows an AC signal to be presented on the tip and ring connections 300 and 302.

A transistor 340 having a collector coupled to the base of the transistor 320, in conjunction with the resistor 342, draw line current from the telephone connection 190 for provision to the electronic inductor 176 to indicate off-hook conditions. The electronic inductor 176 operates in conjunction with the DAC 188, ADC 190 and software control functionality of the DAA. The electronic inductor 176 is also coupled to the "+" terminal of the full wave bridge rectifier 310 via resistors 344, 348, 350 and capacitor 346. The resistor dividers formed of resistors 344 and 348 are utilized to determine if the tip and ring connection 300 and 302 voltages reflect an on-hook condition.

The loop current measurement circuitry 180 is also coupled to the emitter of the transistor 340 in order to measure current levels present on the tip and ring conductors 300 and 302. The tip/ring voltage measurement circuit 178 is coupled to the "+" terminal of the full wave bridge rectifier 310 via the resistor 344.

The DAC 188 and ADC 190 are utilized in the disclosed embodiment to aid in measuring currents and voltages in the tip and ring connections 300 and 302, and for providing related information to the protocol framing and control circuit 192 for provision to the system side circuitry 104. The DAC 188 and ADC 190 are programmable to allow modifications to the current and voltages on the tip and ring connections 303 and 302 (e.g., the line side circuitry 102 can be programmed to draw more current from the tip and ring connections 300 and 302 to lower telephone line voltages as may be required in a specific country).

As with the embodiment of FIG. 4A, the line side circuitry 102 of FIG. 4B may include various other combinations of programmable features. In addition, further exemplary details of specific portions of the programmable line side circuitry 102 of FIGS. 4A and 4B can be found in the references incorporated above, including: U.S. patent application Ser. No. 09/074,896, filed May 8, 1998; U.S. patent application Ser. No. 09/075,451, filed May 8, 1998; and U.S. patent application Ser. No. 09/929,960, filed Sep. 15, 1997.

FIG. 5 is a drawing of exemplary transceiver circuitry 132 and 186 for communicating a serial datastream across the digital isolation barrier 100 of FIG. 1. The disclosed circuitry provides for bidirectional serial communications across the digital isolation barrier 100 in a differential manner. To this end, each of the transceivers 132 and 186 comprise switchable line driver circuitry.

Referring more specifically to transceiver 132, a first differential output comparator 400 is provided for driving signals across the digital isolation barrier 100, while a second comparator 402 is provided for receiving signals from the digital isolation barrier 100. An integrated double-pole double-throw switch 408 is provided to couple either the outputs of the comparator 400 or the inputs of the comparator 402 to the digital isolation barrier 100. Operation of the switch 408 is coordinated with the operation of an integrated double-pole double-throw switch 410 of the transceiver circuit 186.

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Data to be transmitted by the system side circuitry 104 is provided to the non-inverting input of the comparator 400 via a connection 416. Resistors 418 and 420 are coupled in series between system side power and ground to provide a reference voltage (at the common node) to the inverting input of the comparator 400. The reference voltage is determined by the ratio of the resistors 418 and 420, and is set to one half of the power supply voltage or other suitable voltage level.

When the transceiver circuitry 132 is receiving data from the digital isolation barrier 100, the signals provided to the input of the comparator 402 of the disclosed embodiment require DC voltage reference levels for the incoming AC signals. To this end, the non-inverting input of the comparator 402 is coupled to the common node of a resistor divider formed by resistors 424 and 426. Similarly, the inverting input of the comparator 402 is coupled to the common node of a resistor divider network formed by resistors 430 and 432. A system side data output connection 422 is coupled to one output of the comparator 402. A feedback resistor 428 is coupled between this output and the non-inverting input of the op-amp 402 to provide hysteresis for purposes of noise immunity. Similarly, a feedback resistor 434 is coupled between the other output of the comparator 402 and its inverting input.

Current limiting resistors 412 and 414 are coupled between the digital isolation barrier 100 and the poles of the double-pole double-throw switch 410 of the transceiver circuit 186. Differential output comparators 404 and 406 are configured to receive and transmit signals, respectively, in the same manner as the comparators 400 and 402. More specifically, the outputs of the differential output comparator 406 are coupled to a paired side of the switch 410 in order to transmit data signals. The inverting input of the comparator 406 is provided a reference voltage by a voltage divider formed of series connected resistors 452 and 454. The non-inverting input of comparator 406 is coupled to a line side data input connection 450, and receives the input to be provided across the digital isolation barrier 100.

The comparator 404 is configured to provide data to a line side data output connection 436 when the switch 410 is configured as illustrated. Accordingly, the inputs of the comparator 404 are coupled to a paired side of the double-pole double-throw switch 410. A DC bias voltage is established at the non-inverting input of the comparator 404 by a voltage divider formed of resistors 438 and 440. Similarly, a DC bias voltage is provided to the inverting input of the comparator 404 by a resistor divider formed of resistors 444 and 446. A feedback resistor 442 is coupled between one output of the comparator 404 and its non-inverting input to provide hysteresis. Likewise, a feedback resistor 448 is coupled between the opposing output of the comparator 404 and its inverting input.

Control of the double-pole double-throw switches 408 and 410 is synchronized by protocol framing and control circuitry 138 and 192, respectively, as discussed below in conjunction with FIGS. 7-9. Many different transceiver circuit arrangements are possible for driving differential signals across the digital isolation barrier 100, and it is not intended that this embodiment of the invention be limited to any one particular arrangement.

FIG. 6 provides exemplary voltage waveforms depicting the differential voltages across the digital isolation barrier of FIG. 5. More specifically, a first V_{202a} is shown for a typical voltage across the isolation capacitor 202a, while a second V_{202b} is shown for the corresponding differential waveform

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across the isolation capacitor 202b. As illustrated, one of the voltages is at a logic high level while the corresponding voltage is at a logic low level. As will be appreciated by those skilled in the art, utilizing differential voltages across the isolation barrier 100 may improve signal integrity, although single-ended arrangements are also contemplated.

FIG. 7 is a diagram of an exemplary serial frame protocol for communicating information across the digital isolation barrier 100 of FIG. 1 in accordance with the present invention. Because the digital isolation barrier 100 is composed of devices such as capacitors or transformers, communications are achieved via AC waveforms. Therefore, in the disclosed embodiment, it is desirable to use an encoding scheme that eliminates long sequences of zeros or ones in the data.

The serial protocol provides sufficient bandwidth to accommodate data from the CODEC 108, CODEC 108 control, data and status signals, line side circuitry 102 control inputs, line side circuitry 102 status outputs, as well as a number of general purpose input/output signals. It is also contemplated that errors (such as those due to voltage surges) may be accounted for by error correction techniques. One method of detecting such errors is to include redundancy in the transmitting data, such as providing a separate, redundant data packet for each data packet that is transmitted.

The exemplary serial frame 700 of FIG. 3 is composed of a number of components or bit groupings. Specifically, frame synchronization bits 702 are provided to coordinate communications between the system side circuitry 104 and the line side circuitry 102. In the enclosed embodiment of the invention, these frame synchronization bits 702 are provided by the system side circuitry 104, although other configurations are possible. Following the frame synchronization bits 702, data, control and/or programming bits are transmitted across the digital isolation barrier 100 to the line side circuitry 102. In the disclosed embodiment of the invention, in which bidirectional serial communications across the digital isolation barrier 100 are utilized, a number of reversal bits 706 are provided in order to allow sufficient time for the transceiver circuitry 132 and 186 to switch direction. The number of bits required depends on the switching time of the particular transceiver circuitry that is utilized by the DAA. A specific reversal synchronization pattern may be utilized to initiate reversal of the transceiver circuitry.

Next, data, control and/or programming bits are communicated in a serial manner from the line side circuitry 102 to the system side circuitry 104. Idle bits 710 are also provided in the serial frame 700 to provide extra bandwidth (in a predefined frame size) for addition of other capabilities and information.

The data, control and/or programming bits may also include interrupt-type information for use in communicating status changes and/or synchronization. For example, in the disclosed embodiment the system side circuitry 104 responds to all interrupt events received over the digital isolation barrier 100. The system side circuitry 104 uses an interrupt mask register (not illustrated) to determine if interrupt events should be relayed to the host system circuitry 116. In the disclosed embodiment, the circuits which are able to interrupt the system side circuitry 104 are the caller ID circuit 158 and the ring/LPR detection circuitry 164. Any activity from these circuits should be detected to allow the system side circuitry 104 to wake up (at least partially) and validate ring and/or caller ID data.

One contemplated encoding protocol involves transmitting data across the digital isolation barrier 100 at half of the

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clock rate. In this scheme, a "0" is coded as a logic level low to a logic level high transition, while a "1" is coded as a transition from a logic level high to a logic level low transition. For example, if a 4 MHz clock is provided to the line side circuitry 102, a 2 MHz signal derived from the clock signal may be used as a bit clock for serial communications. Using this arrangement, 128 bits are available in serial form during one period of a 16 kHz sample rate with a 2.048 MHz clock ($128 = 4.096 \text{ MHz} / (2 * 16 \text{ kHz})$). It is contemplated that control data may flow at either a lower or higher rate than data from the CODEC 108.

A specific embodiment of a protocol for digital serial communications across the digital interface barrier 100 is provided in attached Appendix A. The protocol disclosed therein is exemplary in nature, and those skilled in the art will recognize that numerous variations are possible.

FIG. 8 is a flow chart of exemplary serial communication steps performed in accordance with the present invention by one embodiment of the system side circuitry 104 of FIG. 1. Following application of power in step 800, the system side circuitry 104 enters a wake-up or resynchronization mode in step 802. Next, in step 804, the transceiver 132 transmits a synchronization packet. The system side circuitry 104 then awaits signals from the line side circuitry 102 indicating that synchronization has been achieved. If synchronization has not been achieved as determined in step 806, a counter is examined in step 808 to determine if a predetermined time-out value has been reached. If not, the process returns to step 806. If the time-out value has been surpassed, the process returns to step 804 where an additional synchronization packet is transmitted.

If synchronization has been achieved as determined in step 806, the process continues to step 810 where serial data, control and/or programming signals are transmitted or received by the transceiver 132. Following completion of the serial communications, an optional low power mode is entered in step 812. Next, in step 814, the system side circuitry 104 awaits a wake-up signal or service request from either the host system circuitry 116 or the line side circuitry 102. Once such signal is received, the process returns to step 802.

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FIG. 9 is a flowchart showing exemplary serial communication steps performed in accordance with the present invention by the line side circuitry 102 of FIG. 1. Following power-on in step 900, the line side circuitry 102 enters an optional sleep or listen mode. Next, in step 904, the line side circuitry 102 determines if a synchronization packet has been received from the system side circuitry 104. If not, the line side circuitry determines (step 906) if an interrupt has been generated by any of the circuitry connected to the telephone network 110. If an interrupt has not been received, the process returns to step 902. If an interrupt has been received, the line side circuitry 102 exits sleep mode in step 908. A signal is then communicated to the system side circuitry 104 in step 910 to request synchronization. It is noted that the precise ordering of the steps 904-906 is not considered critical to the invention.

If a synchronization packet has been received as determined in step 904, the line side circuitry 102 exits sleep mode in step 914. Following either of steps 910 or 914, the line side circuitry 102 determines if synchronization with the system side circuitry 104 has been achieved. If not, a time-out counter is examined in step 916 to determine if a predetermined amount of time has expired without synchronization. If not, control turns to step 910 and synchronization is again initiated. If the time-out value has been reached, or if an interrupt was not found in step 906, step 902 is repeated and the line side circuitry enters an optional sleep or listen mode.

Thus, a data access arrangement has been described in which the high voltage isolation barrier and other circuitry is configured such that information may be communicated between the system side circuitry and the line side circuitry in a digital format. A high voltage isolation barrier according to the invention provides an inexpensive and physically compact way to pass digital signals in both directions utilizing as few as one capacitor or one transformer.

In view of the above detailed description of the present invention and associated drawings, other modifications and variations will now become apparent to those skilled in the art. It should also be apparent that such other modifications and variations may be effected without departing from the spirit and scope of the present invention.

APPENDIX A

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1. SYSTEM SIDE CIRCUITRY

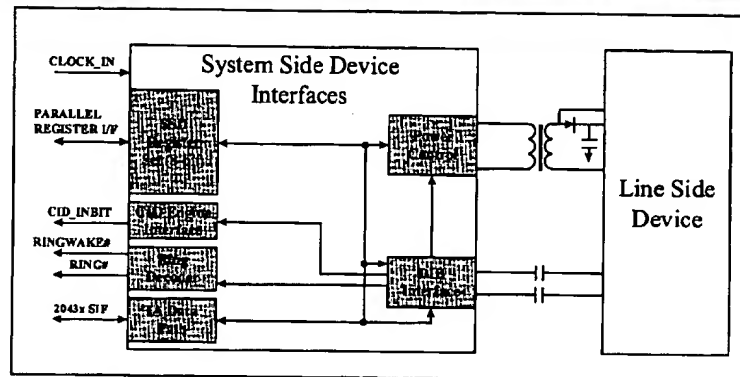


Figure 1. System Side Device block diagram

The System Side device contains the following functional blocks, as shown in Figure 1.

- DIB Interface
- Power Control
- Caller ID Engine Interface
- Ring Decoder (generates RINGWAKE#)
- IA Data Channel (AC Link support TBD)
- System Side Device Register Set

The System Side Device, as shown above, consists of two major interfaces. Interfaces (via the DIB) to the Line Side Device are shown to the right, and interfaces to the host device are shown to the left. This document describes one implementation of the data protocol used on the DIB to send and receive data, control, and status information, as well as the DIB power control, CID and Ring Interfaces, IA Data Path, and an 8-bit register set available to the host. Existing BASIC logic uses 8-bit registers to interface to the host, with 5 address lines to select registers. The SSD register set directly interfaces to this existing BASIC register logic, using one of the existing unused chip selects.

2. DIB Data Interface – System Side

2.1. Requirements

The DIB protocol is used to pass all required register and control data over the Digital Isolation Barrier, including, at minimum, one Transmit and one Receive Data Word per 16 kHz sample time, control/status bytes, and optional redundant Transmit and Receive Data words. A means of re-transmitting packets received in error should be implemented since no error correction exists at the Line Side Device receiver.

2.2. Proposed Implementation

2.2.1. Assumptions

The System Side implementation of the DIB protocol assumes the following:

- The Line-Side Device (LSD) is a slave device to the System Side Device (SSD). The LSD does not initiate a transfer across the DIB unless it is requested, except when asleep.

Note: This implies that any semi-continuous monitoring of Line Side status by the System Side requires the System Side to poll the LSD.
- The Line Side Device will only communicate over the DIB to the System Side Device using the DIB packet protocol (i.e., 4 MHz clock is running), and the Line Side has been synchronized to the System Side.
- When the DIB packet protocol is operational, the System Side Device initiates an FSP based frame every 16 kHz time period.
- If no FSP frame is sent by the SSD, the LSD goes into 'listen' mode. GPIO activity on the Line Side, or an FSP frame sent by the SSD awakens the LSD.
- The System Side Device should write to the power control register (EXMSC, Register 000001) to power down portions of the Line Side Device prior to reducing the clock frequency.
- When a wake up sequence (FSP) is received from the LSD while the Line Side Device is asleep (due to GPIO activity), the System Side immediately raises the clock frequency and begins communicating to the LSD using the DIB Protocol.
- Once synchronization is established across the DIB, both sides can count clock cycles (of the 4 MHz input clock, or the 2 MHz clock derived from it).
- It takes less than two (2) 2-MHz clock cycles for the DIB transceivers to switch from one direction to another. Two information bit times are allocated every time the direction of communication is changed.
- The System Side Device is responsible for generating RING# and RINGWAKE# signals appropriate for the Caller ID Engine, using output from LSD circuits over the

DIB. These generated signals should provide Pulse Dial rejection, Extension off-hook rejection, and invalid RING frequency or amplitude rejection.

2.2.2. Bandwidth Summary

Given the 4 MHz clock frequency and the signaling format required across the DIB, a total of 128 information bits may be transmitted across the barrier within a 62.5 microsecond frame (1 sample period, at 16 kHz).

Obviously, within a frame of 128 bits, it is essential to transmit and receive one 16-bit sample of data across the barrier. It is also necessary to provide for a method to transmit control information from the system side to the line side, and transmit status information from the line-side to the system side.

2.2.3. DIB Ping-Pong Protocol Summary

SSD	FSP	Data1	Control1	Data1bis	RSP	S				S	Idle
LSD						S	Data2	Control2	Data2bis	S	Idle
Frame											
Bits	0..3	4..21	22..39	40..57	58..61	62..63	64..81	82..99	100..117	118..119	120..127

Figure 2. Bit allocation over the DIB channel for one sample time (frame)

The Ping-Pong Protocol of this implementation is designed to operate in the same manner at all times, in order to simplify system design. It is assumed that sending additional data across the two data capacitors for the full frame requires an insignificant incremental amount of power compared to other send-if-necessary schemes.

As shown in Figure 2, the SSD transmits the Frame Synchronization Pattern (FSP) starting at bit 0 of the 16 kHz frame, then it transmits a data packet, a control packet, and (optionally) another data packet. It ends its transmission with a Reversal Synchronization Pattern (RSP), which signals a reversal of direction to the line side. Both sides then "waste" bits 62 and 63 in order to switch the transceiver transmission direction, then the LSD transmits its own data packet, etc. An alternate frame packet, in which the SSD omits the Data1bis packet, and the RSP follows the Control1 packet, is allowed for system implementations where the added robustness is not necessary.

In the SSD to LSD direction, the first data packet, Data1, consists of the data sample to be transmitted for the current sample period. The next control packet, Control1 is for control information transmission. Finally, the second data packet Data1bis, is intended as a simple error correction (robustness) mechanism: the same data sample (as in the Data1 packet) is simply retransmitted in this packet.

The LSD follows the same procedure in sending packets to the SSD. The LSD does not reverse the interface to the DIB (i.e., become a transmitter) until successfully receiving the RSP. After enabling its DIB outputs, the LSD sends the Data2 packet, which consists of the received data for the current sample period. The next packet, Control2, is used for status transmission to the SSD and is null unless the SSD requested a Read In Control1 or a GPIO based interrupt is generated by the LSD. The third packet, Data2bis, contains a

copy of the data in the Data2 packet, for robustness. If the *Data1bis* packet was not transmitted by the SSD, the LSD omits sending the *Data2bis* packet.

The System Side Device should transmit a second control packet, even if it is not required. If the control packet is not required in one or both directions, a special null control packet will be transmitted. This scheme is necessary to maintain a simple and consistent master-slave relationship in the DIB protocol.

If the SSD only supports the alternate data format (which excludes *Data1bis*), the LSD will detect that the RSP was received before *Data1bis*, and it will also cancel its own transmission of *Data2bis*.

If the Line Side Device receives both the *Data1* and *Data1bis* packets in error, the LSD will use the last error-free received sample for the current frame.

2.2.4. Frame Synchronization Pattern Definition

The Line Side device uses the FSP to generate a sample clock that is synchronized to the System Side device at all times. For all expected HCF and HSF data modem implementations, this sample clock will be 16 kHz, although it could be a lower rate if the System Side simply initiated transmission of the FSP, Data, and Control at longer intervals than 62.5 microseconds.

The Frame Synchronization Pattern (FSP) consists of a fixed pattern of 8 data bits (equivalent to 4 symbols). It is transmitted by the SSD to the LSD at the beginning of each frame. The FSP is designed so that it does not correspond to a valid sequence of '0' or '1' symbols, even if synchronization is lost.

The FSP consists of the following pattern of data bits: 11110000, which correspond to the sequence 'AABB' of symbols.

2.2.5. Reversal Synchronization Pattern Definition

The Line Side device uses the RSP to determine when to reverse transmission on the DIB, and whether it will transmit one or two data packets to the system side.

The Reversal Synchronization Pattern (RSP) consists of a fixed pattern of 8 data bits (equivalent to 4 symbols). It is transmitted by the SSD to the LSD at the end of its transmission (after *Data1bis* or after *Control1*). The RSP is designed so that it does not correspond to a valid sequence of '0' or '1' symbols.

The RSP consists of the following pattern of data bits: 00001111, which correspond to the sequence 'BBAA' of symbols.

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2.2.6. Packet Definitions

The following sections show the format for each of the packets sent by or received by the System Side device. The packets are shifted over the DIB from left to right as shown in the tables below, ending with the parity bit.

For simplicity, all packets consist of 18 bits and end with a single parity bit.

2.2.6.1. Packets Transmitted by the System Side Device

2.2.6.1.1. Data1 Packet Definition

Data		1	PAR
<MSb>	16 bits	<LSb> 1 bit	1 bit

- DATA: 16-bit sample, with the most significant bit shifted first.
- 1: This symbol is unassigned, and is transmitted as a '1'.
- PARITY (PAR): Parity bit, used for error detection. Odd parity is calculated using the first 17 bits of the packet.

2.2.6.1.2. Control1 Packet Definition

W/R	Address	H/L	Control	1	PAR
1 bit	6 bits	1 bit	8 bits	1 bit	1 bit

- WRITE/READ (W/R): In a control packet sent by the system side, this bit indicates whether this is a write or a read request. W/R is set to '1' for a write request, to '0' otherwise.

Note that for a read request, the system side device sends a packet with '0' control bits, used to pad the control packet to the full 18 bits.
- ADDRESS: This field contains the address of the control/status register being transmitted.
- HIGH/LOW (H/L): Control bit used to indicate whether the SSD is addressing the upper (high) or lower (low) byte of the 16-bit LSD register. This bit is set to '1' if the high byte is being addressed, to '0' otherwise.

Note: The Line Side Device DIB interface implements logical 8-bit addressing using the Address (6-bit) and H/L bit. The high or low byte is transmitted independently of the other. Thus, the System Side Device need not read or write a high byte following a low byte or vice versa.
- CONTROL: This field contains the control/status byte.
- 1: This symbol is unassigned, and is transmitted as a '1'.

- **PARITY (PAR):** This bit is a parity bit, used for error detection. Odd parity is calculated using the first 17 bits of the packet.

2.2.6.1.3. Data1bis Packet Definition

The contents of the *Data1bis* packet are identical to those of the *Data1* packet.

2.2.6.2. Packets Received by the System Side Device

2.2.6.2.1. Data2 Packet Definition

Data		ERR	PAR
<MSb>	16 bits	<LSb>	1 bit

- **DATA:** When control bit DATAMODE in the Line Side Device MCR register is a '0', the DATA field contains the received 16-bit sample ADC, with the most significant bit shifted first.

When control bit DATAMODE in the Line Side Device MCR register is a '1', the Data consists of the sampled output of the Caller ID and RDO/LPR (and ~LPR) comparators, and the voltage regulator clamp, in the following format. For Caller ID and RING, the 3 bits represent 3 1-bit comparator outputs sampled at 48 kHz. The most significant bit of each field is the 'oldest' bit. Caller ID data and RING data are also available via polling Line Side Register TRSTAT. Note that it is expected that only the most recent of the RDO/LPR and ~LPR output bits will be used, resulting in an effective sample rate of 16 kHz for these outputs.

D15	D14	D13	D12	D11	D10	D9	D8	D7	D6	D5	D4	D3	D2	D1	D0
0	VCR[2:0]			0	CID DATA[2:0]			0	~LPR[2:0]			0	RDO/LPR[2:0]		

- **ERROR (ERR):** If the Line Side device sets this bit, this indicates that an error was detected in the received *Data1* packet originally transmitted by System Side device.

A counter is implemented on the System Side device to track how many times the Line Side indicates an error in transmitted data packets. The host should be able to reset the counter on demand by a write to the counter register.

- **PARITY (PAR):** This bit is a parity bit, used for error detection. Odd parity will be calculated using the first 17 bits of the packet.

2.2.6.2.2. Control2 Packet Definition

INT	Address	H/L	Control	ERR	PAR
1 bit	6 bits	1 bit	8 bits	1 bit	1 bit

- **INTERRUPT (INT):** The Line Side device sets this bit when an "interrupt" event occurs in the Line Side device register set. The System Side Device should respond to this bit being active by reading the Line Side Device GPIO Status register.

- **ADDRESS:** This field contains the address of the control/status register being transmitted. In the case of a write, the address written to is echoed back to the System Side Device by the Line Side Device.
- **HIGH/LOW (H/L):** Control bit used to indicate whether the SSD is addressing the upper (high) or lower (low) byte of a 16-bit LSD register. This bit is set to '1' if the high byte is being addressed, to '0' otherwise.

Note: The Line Side Device DIB interface implements logical 8-bit wide addressing using the Address (6-bit) and H/L bit. The high or low byte is transmitted independently of the other. Thus, the System Side Device need not read or write a high byte following a low byte or vice versa.

- **CONTROL:** This field contains the control/status byte to be written/read.

In the case of a response to a write, the control byte written to the Line Side Device is echoed back to the System Side Device. If the echoed byte does not match the original byte written by the SSD, the SSD automatically does not set the 'OK' bit in the LSDSTAT register (\$00), and instead increments the ERRCNTL2 counter.

- **ERROR (ERR):** If the Line Side device sets this bit, this indicates that an error was detected in the received *Control1* packet originally transmitted by System Side device.

A counter is implemented on the System Side device to track how many times the Line Side indicates an error in transmitted data packets. The host should be able to reset the counter on demand (by writing to it). Since erroneously received control packets are discarded by the Line Side Device, the System Side Device retransmits these packets during the next frame.

The SSD increments the ERRCNTL1 counter, and automatically re-transmit the control packet which failed. Successive failures will continue to increment the ERRCNTL1 counter until the counter overflows (reaches a hex value of 'F'). This overflow will cause the SSD to set the DIBFAIL status bit, and to generate a host interrupt (masked using the IMASK register). It is expected that the host driver software will reset the clock output to the LSD, resetting it and causing it to go on-hook.

- **PARITY (PAR):** This bit is a parity bit, used for error detection. Odd parity will be calculated using the first 17 bits of the packet.

Note: If the SSD finds a parity or non-legal symbol error in the *Control2* packet, all bits in the packet, including INT, are discarded.

2.2.6.2.3. Data2bis Packet Definition

The contents of the *Data2bis* packet are identical to those of the *Data2* packet. The only difference is that the ERR bit is only set if the LSD detected an error in the *Data1bis* packet received.

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2.3. DIB Synchronization – System Side

Synchronization will be achieved/maintained between the SSD (master) and LSD (slave) by means of a special sequence of symbols (the FSP) sent by the System Side device at the beginning of each frame or whenever synchronization is lost. When sufficient power is present (i.e., the power clock is being received), the LSD will always respond to a frame that begins with the FSP. When power is present, but the LSD is 'asleep', GPIO activity will cause the LSD to send FSP to the SSD, to request wake-up. A state-diagram is included in Figure 3 below:

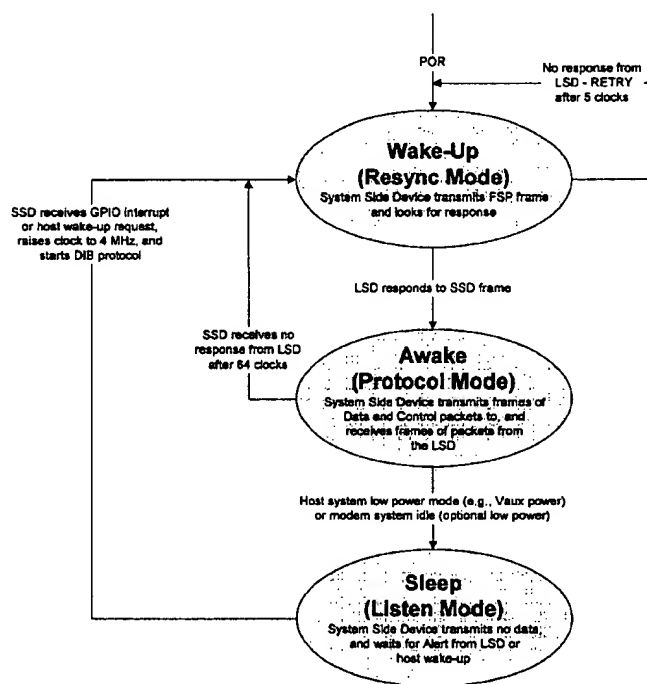


Figure 3. System Side Device DIB States

2.4. DIB Power On Reset

When the system is powered up, the System Side DIB interface defaults to Resync Mode, in which it is a transmitter, sending a frame of data and control information to the LSD. The System side waits for a normal response from the LSD to indicate that the DIB and LSD are operational. The System Side device then enters normal operation (Protocol Mode), sending a frame of data and control information to the LSD each frame (sample) time. Each time it completes transmission of the frame, the system side reverses the DIB and "listens" for the return packets from the LSD. If it does not receive anything within the

following 5 bit times, synchronization between the two devices has been lost, and the SSD reverses the DIB again and re-transmits the frame (having re-entered Resync Mode).

2.4.1. Cold Reset

The System Side Device may at any time perform a cold reset of the LSD by stopping the power clock altogether for a predetermined number of milliseconds, allowing the VDD voltage of the LSD to dissipate. The System Side may then re-start the Line Side Device by turning on the clock and performing the synchronization described above. This reset mechanism is slow and should be used only as a last resort. Alternatively, the System Side Device may write to the LSD's ID register (VEN1, Register 16) to reset all register bits to default status.

2.5. System Side Wake-Up Summary

If the Line Side is 'asleep' (i.e., the device is in Listen Mode and the power clock is 140 kHz) and activity is detected from any GPIO configured to generate an interrupt, the Line Side will generate an alerting signal to the System Side Device. Immediately after alerting the SSD, the LSD will switch its interface to receive mode.

The alerting signal will consist of 4 symbols, 'AABB', at the 70 kHz bit rate (1/2 the power clock). This will correspond to data bits of '11110000'. Note that 'A' and 'B' have been chosen as noise tolerant special signals because they generate a transmit signal which is a sub harmonic of the 140 kHz power clock and the 70 kHz bit clock and will therefore be unlikely to be generated by board or clock noise.

Upon detection of the activity on the DIB data lines, and verification of the 'AABB' signal, the System Side device raises the power clock frequency to 4 MHz, and begins transmitting a frame beginning with FSP.

2.6. System Side Error Detection

The System Side can detect and track several types of errors in the transmitted and received data and control packets, as described below. Eight error counters exist in the System Side Device to track DIB performance. Six counters are dedicated to data errors for the six defined packets for the DIB (*Data1*, *Data2*, *Control1*, *Control2*, *Data1bis*, and *Data2bis*). Two more counters are used to count synchronization errors over the DIB.

2.6.1. Errors in the Data

The System Side Device increments one of three error counters based on incorrectly received *Data2*, *Control2*, or *Data2bis* packets from the Line Side Device. If the received packets are error free, then the System Side Device increments the three error counters corresponding to the *Data1*, *Control1*, and *Data1bis* packets sent from the SSD to the LSD, depending on the status of the ERR bits in each of the received packets from the LSD.

Errors can consist of non-legal data symbols, or parity errors, as described below.

2.6.1.1. Non-Legal Data Symbols

If the System Side receives an 'A' or 'B' signal at any time other than when the Line Side Device is asleep, one of two types of errors has occurred. Either one half of one symbol ('0' = '01' or '1' = '10') has been corrupted, resulting in a half-symbol error, or there has been a loss of synchronization due to a clock slip on the DIB. Both will be treated as a non-legal Data Symbol.

In the case of a clock slip, the DIB will be re-synchronized by the next FSP based frame sent by the System Side Device, so no special action is necessary.

If the Line Side Device has received an 'A' or 'B' signal at any time after the reception of the FSP, and before RSP, either one half of one symbol has been corrupted, or there has been a loss of synchronization due to a clock slip on the DIB. The Line Side Device will determine which error has occurred by if/when the RSP is received.

If the RSP is received on time, the Line Side device detects a Non-Legal Data Symbol error, and communication over the DIB continues without a resynchronization. The Line Side device reacts by using the other data packet or discarding the control packet, as appropriate, and sets the appropriate ERR bit in its frame response (which the SSD will count, as described above). If the RSP is received late or not at all, then the LSD will respond to the error by going to Listen Mode until the SSD sends another frame. Thus, the error will then be detected as a synchronization error.

2.6.1.2. Parity Errors

If, at the end of the *Data2*, *Control2*, or *Data2bis* packets, the Parity bit for the first 17 bits in the packet does not agree with the SSD calculated parity of the data in the packet, then a Parity Error is detected. A Parity error in this case indicates that an odd number of symbols have changed from '0' to '1' or vice versa. The SSD will then increment the error counter corresponding to the appropriate received packet. If the Parity bit of any packet is received as an 'A' or 'B' symbol, it is corrupted and the System Side detects a Non-Legal Data Symbol error.

If, at the end of the *Data1*, *Control1*, or *Data1bis* packets, the Parity bit for the first 17 bits in the packet does not agree with the LSD calculated parity of the data in the packet, then the Line Side Device detects a Parity Error. If the Parity bit of any packet is received as an 'A' or 'B' symbol, it is corrupted and the Line Side detects a Non-Legal Data Symbol error. The Line Side Device reacts by using the other data packet or discarding the control packet, as appropriate, and sets the appropriate ERR bit in its frame response (which the SSD will count, as described above).

2.6.2. Time Out and Synchronization Errors

In some cases, the Line Side response to an error is to stop communicating with the System Side device. This indicates that the System Side device should re-awaken the Line Side device with a frame beginning with FSP. At each occurrence (other than POR), the System Side increments an error counter indicating that the LSD synchronization was lost.

Also, during the Wake Up sequence it is possible for the Line Side Device to miss the System Side synchronization signal, 'AABB'. This will require the SSD to resend the frame. In this case, the SSD should increment the eighth error counter, allowing the

system to track how long it takes to resynchronize the DIB at initial power up, wake-up, or during a loss of synchronization.

In the event of a wake-up, it is important that the LSD and SSD do not wait the same number of clock cycles (5 cycles of the 2 MHz bit clock) before re-transmission. This will prevent repeated collisions on the DIB of the SSD FSP and the LSD Alerting signal (FSP), and subsequent failure of the system to wake up.

2.6.3. Error Condition Pseudo-Code

The following pieces of pseudo-code show how the System Side implementation of the DIB protocol handles various error conditions.

```

If System side detects error in Data2 then
    System side uses data sample in Data2bis instead;
    System side increments Data2 error counter.
Endif

If System side detects error in Data2bis then
    System side uses old receive sample;
    System side increments Data2bis error counter.
Endif

If System side detects error in Control2 then
    System side resends control packet in Control1 of the following frame;
    System side increments Control2 error counter.
Endif

If System side receives ERR in Data2 then
    System side increments Data1 error counter.
Endif

If System side receives ERR in Data2bis then
    System side increments Data1bis error counter.
Endif

If System side receives ERR in Control2 then
    System side increments Control1 error counter.
    System side resends control packet in Control1 of the following frame;
Endif

If (line side loses synchronization (loss of clock, no FSP, etc...))
    Line side stops transmission;
    System side detects loss of contact;
    System side re-transmits frame;
    System side increments synchronization error counter;
    Line side detects FSP;
    Communication resumes;
Endif

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If System side receives no reply to FSP during (re)synchronization
  System side times out;
  System side re-transmits frame;
  System side increments synchronization retry error counter;
  Line side detects FSP;
  Communication resumes;
Endif

```

2.7. System Side Interrupt Detection/Handling

A number of Line Side circuits can require SSD event handling on an interrupt (or system wake-up) basis. Since only GPIO can generate interrupts (using the AC'97 specification as a model), all such circuits will be connected to LSD GPI. By default, the circuits which should be able to interrupt the SSD are the Caller ID detector and Ring detector comparators. Any activity (edges) from these circuits should be detected to allow the system to wake up (at least partially) and validate ring and/or Caller ID data.

The System Side Device responds to all interrupt events received over the DiB. The System Side Device uses an interrupt mask register to determine if interrupt events should be relayed to the host.

2.7.1. Detection Methods

2.7.1.1. When DiB Protocol is active (Protocol Mode)

When the DiB protocol is running, the Line Side Device provides a means of interrupting the host via the INT bit in the *Control2* packet. To enable these features, the GPIO should be powered on (in the LSD EXMSC register), the GPIO direction should be programmed to 'input' (default), the GPIO Sticky register should set the GPI to be edge sensitive, the GPIO Wake up mask should enable the GPI to generate interrupts, and the DATAMODE control bit in the LSD MCR register should be set to a '1'.

Then, when an edge is detected on any of these interrupt generating GPI, the GPIO Status register will contain a '1' for the input that generated the edge, and the LSD will return a '1' for the INT bit in the *Control2* register. The LSD will continue to return INT=1 until the host/SSD writes to the GPIOS register, resetting the sticky bit corresponding to the interrupt.

On reception of the *Control2* register, the SSD will detect INT=1, and will set the corresponding INT bit in the LSDSTAT register and activate a hardware interrupt line if the INTE control bit is set to '1'. It is expected that this hardware interrupt line will be routed to the Host for most projects.

2.7.1.2. When DiB Protocol is inactive (Low Power Mode)

Alternatively, when the system is asleep (with the 140 kHz clock running), the Line Side Device may interrupt the SSD by sending an FSP ('AABB') sequence of signals over the DiB.

The SSD will detect the signal from the LSD, raise the clock on the DiB interface to 4 MHz, and send a full frame beginning with FSP to the LSD. This frame should consist of a Control channel Read of the LSD GPIOS register.

After synchronization between the two devices, the Interrupt detection mechanism will proceed as described in Section 2.7.1.1.

2.7.2. Handling Required Interrupts

Three interrupts are necessary to overall system function. They are the Ring Detector, Line Polarity Reversal Detector and Caller ID Detector interrupts (GPI1, GPI2 and GPI0, respectively, for the LSD).

2.7.2.1. Ring Detection

Since the System Side Device will generate the RINGWAKE# signal for the Caller ID Engine, it is necessary for the Ring Detector output to:

- (1) Cause an Interrupt to the SSD.
- (2) Wake up the DIB if not already in Protocol Mode.
- (3) Process the sampled RDO/LPR bit stream from the LSD.
- (4) Provide the RINGWAKE signal to the Caller ID Engine.

Thus, while the System is under Vaux power, with only 140 kHz over the DIB, the incoming Ring generates an interrupt over the DIB (LSD will send FSP to SSD). The SSD then raises the DIB clock to 4 MHz, and synchronizes with the LSD. The host is not running, and may take several seconds to awaken. The SSD may automatically detect that the Interrupt source is GPI1 (RDO/LPR) or GPI2 (~LPR), set the DATAMODE bit in LSD register MCR, and begin sending the RDO/LPR samples to the Ring Decoder.

The Ring Decoder then determines if the incoming Ring/LPR activity is valid. If so, RINGWAKE# will be asserted to the Caller ID Engine. If not, the DIB will be put back into Low Power Mode (140 kHz clock) after resetting the interrupt.

When the System is in Protocol Mode, fully awake (host, SSD, and LSD all running normally), and on-hook, the DATAMODE bit should be a '1', and the RDO/LPR bits should be passed directly (after Inversion) to the host/DSP as RING#. This will provide a half-wave rectified Ring Detector output for the host to use/process when Ring is received. In this case, the Caller ID Engine is not used.

2.7.2.2. CID Detection/Decode (D3Cold)

The Caller ID Detection/Decoding circuitry may work for the D3Cold case, in which the host is not functioning, the SSD and LSD are Idle, and the DIB is running with the reduced clock (140 kHz). When activity is received from the Caller ID detector output on the LSD, this may:

- (1) Cause an Interrupt to the SSD.
- (2) Wake up the DIB if not already in Protocol Mode.

- (3) Cause the CID_DATA output bits (48 kHz sample rate, 1-bit per sample) to be routed to the Caller ID Engine input (waking the Caller ID Engine).

While the system is under Vaux power, with 140 kHz over the DIB, the incoming Caller ID Data generates an interrupt over the DIB (the LSD will send FSP to the SSD). The SSD will then raise the DIB clock to 4 MHz, and synchronize with the LSD. The host is not running, and may take several seconds to awaken. Therefore, the SSD may automatically detect that the interrupt source is Caller ID (would appear to be GPI1 or GPI2 – same as Ring), set the DATAMODE bit in LSD register MCR, and begin sending the CID_DATA samples to the Caller ID Engine.

The Caller ID Engine then determines if the incoming Caller ID data is valid. If so, the Caller ID Engine will assert a PME event, waking the host system, and store up to 256 bytes of Caller ID data. This functionality is already present in the BASIC 2.15 device and will require little if any change. If the Caller ID Engine determines that the data is not valid, the DIB will be put back into Low Power Mode (140 kHz clock) and the Caller ID Engine will reset to idle state, after resetting the interrupt.

When the System is in Protocol Mode, fully awake, and on-hook, the Caller ID Detector in the LSD is not used. Instead, the 16-bit samples received from the line via the IA will be routed directly to the DSP/Host for processing. This requires that the DATAMODE bit in the LSD MCR register be set to a '0'.

2.7.3. Handling Other Interrupts

The system implementation is able to handle other, as yet unspecified, interrupts. This will allow the addition of new features without changing the SSD or LSD design. Such new features, if necessary, generate interrupts. These interrupts can, if needed, generate a host interrupt by setting the interrupt mask registers (IMASKx) and interrupt enable bit (INTE) in the LSDSTAT register.

2.7.3.1. Unintentional Off-Hook

If an off-hook detector is added to the LSD, the output of this detector may be routed to a GPI, and used as an interrupt to the System Side Device.

If no detector is added to the LSD, the System Side Device to periodically raises the Clock to 4 MHz to detect if the Line Side Device is drawing current (or if an extension is off-hook). Then the SSD will configure the Monitor ADC to measure the voltage at Tip/Ring, and generate an interrupt to the Host/BASIC if this voltage is below a pre-determined threshold. If not, the DIB clock will be reduced back to 140 kHz and both SSD and LSD will return to Sleep state.

Therefore, although the function can be implemented, this capability will not use a pre-assigned GPI or generate an interrupt over the DIB from the LSD to SSD.

2.7.3.2. Active Power Control

A means for Active Power Control exists in the current Line Side Device. An automatic voltage clamp is provided, which prevents the VDD voltage on the Line Side Device from exceeding 5.4 VDC. When the voltage exceeds this limit, bit VCR is set to a '1', and current is shunted from the VDD power supply through the clamp circuit, to reduce VDD.

This output is connected to GPI3 of the Line Side Device and may be configured to cause an interrupt to the SSD.

If this interrupt is received, while the DIB clock frequency is 140 kHz, then the LSD will generate an interrupt over the DIB (LSD will send FSP to SSD) if the LSD GPIO registers are programmed to generate an interrupt from GPI3. The SSD will then raise the DIB clock to 4 MHz, and synchronize with the LSD.

At this time the host software will reprogram the SSD drivers to provide less drive current, thereby lowering the VDD voltage on the LSD. This will require that the host software: (1) read the VDD voltage using the 6-bit monitor ADC on the LSD; (2) change (lower) the drive current of the power supply/clock on the DIB; and (3) read the VDD voltage again, repeating until the VDD voltage is reduced to the desired operating range.

If such active power control is not necessary, GPI3 on the LSD need not be programmed to generate interrupts, in which case the LSD voltage clamp circuit will automatically limit LSD VDD to about 5.4 VDC. In this case the LSD device will consume excess current when the voltage clamp is shunting/clamping VDD. This may not be practical for low power modem implementations (e.g., in portable computers).

3. DIB Power Interface - System Side

3.1. Requirements

The System Side Device functions as the source of both the master data clock and the power for the Line Side Device. The master data clock consists of one or two drive frequencies. Since LSD Power will also be derived from this clock, the master clock may also be able to provide several different drive current levels as needed for different operating/power consumption modes of the Line Side Device.

In addition, the SSD may be able to monitor the Line Side Device power status to prevent under or overdriving the voltage input of the Line Side Device.

3.2. Proposed Implementation

The System Side Device includes one 8-bit Clock/Power Control register, CLKPWR. This register includes:

Name	Bit#	Description	Default
Ciks High	0-2	Controls the duty cycle of the output clock/power. '000' or '111' = 50% duty cycle. '001' - '110' = 1 to 6 7ths high, 6 to 1 7ths low. This control can be used to control the total amount of power delivered to the LSD.	000
Freq	3	Controls output clock frequency. '1' = 4.096 or 4.032 MHz '0' = 140 kHz	1
Power Out	4-6	Controls clock output driver current. '000' = maximum driver current, '001'-'111' = TBD	000
Ciken	7	Controls clock output driver.	1

		'1' = enable, '0' = disable (both outputs may be held high or low)	
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The System Side Device monitors the Line Side Device voltage in two ways. First, the output of the LSD VDD voltage clamp circuit (VCR) is connected to GPI3. This output will be a '1' when the LSD voltage exceeds 5.4 VDC and the clamp is actively controlling Line Side voltage. The LSD will be configured to generate an interrupt when this GPI is a '1', or when a rising edge is encountered. This will allow the SSD to detect when the power output to the LSD is more than required.

Second, the System Side Device can be used to measure the Line Side supply voltage. The Line Side device contains a Monitor ADC (6-bits) which can be connected to the voltage supply rail (using a resistor divider to scale the VDD down to the 0V – 3.5V domain of the ADC). The host can use this Monitor ADC to periodically check the Line Side Device VDD and to adjust the output current or frequency of the clock used to power the LSD accordingly.

The output of the voltage clamp is also available to the SSD by setting the DATAMODE bit to a '1' in the LSD MCR register, and checking bit 12 of the 16-bit RX data word at each sample time. Or, when DATAMODE is a '0', the SSD can read the LSD TRSTAT register (upper half) and check bit 4 of the byte that is read.

4. CID Engine Interface

4.1. Requirements

In D3Cold mode, the Caller ID Engine in the BASIC 2.xx device is used to receive and store up to 256 bytes of Caller ID data from the phone line interface while the host is not available. The System Side Device may translate Caller ID data from the Line Side Device (via the DIB data lines) into a format compatible with the Caller ID Engine already implemented in the BASIC 2.xx device.

When the system is not in D3Cold mode, the HSF host software or HCF data pump device will receive 16 bit data words from the IA (via the *Data2/Data2bis* packets) and decode the FSK data. The Caller ID Engine is not used in this case.

4.2. Proposed Implementation

The Line Side Device samples the incoming analog Caller ID signal (when control bit ~RD/CID in the MONADC register is a '1') at a 48 kHz rate. The resulting 1-bit samples will be placed into the LSD TRSTAT register, and if the DATAMODE bit in the LSD MCR register is a '1', the TRSTAT register will be transmitted to the SSD in the *Data2* and *Data2bis* packets.

To enable the 48 kHz 1-bit serial path from the SSD Caller ID Engine Interface output to the BASIC device (CID Engine Input), the CIDDEN bit may be set to a '1' in the CIDENGCTL register. Received CID_DATA bits (3 at a time) from the DIB are copied to the CID_DATAx[2:0] fields of the CIDENGCTL register. Two such fields are defined. Thus, there will be no conflict between the writing of the newest group of 3 bits by the SSD

logic and the reading of any of the bits by the shift register which outputs the bits to the BASIC device.

The default values for both CID_DATAx fields, as well as CIDEN and PING/PONG bits in the CIDENGCTL register, are '0'. After CIDEN is set to '1', bits 8-10 of the *Data2* (or *Data2bis*, if *Data2* contains an error) are copied to the CIDENGCTL register. When the PING/PONG bit is a '0', the three bits are copied to the CID_DATA1 field of the register, and the PING/PONG bit is set to a '1'. When the PING/PONG bit is a '1', the three bits are copied to the CID_DATA2 field of the register, and the PING/PONG bit is reset to '0'.

When the CIDEN bit is a '1', and the PING/PONG bit has changed state, the SSD will begin shifting the most recently received bits (oldest bit first) out to the CID Engine in the BASIC device, using the 48 kHz clock. At the 4th (and subsequent) clock after the three bits begin to be shifted, if the PING/PONG bit has not changed state, the output to the CID Engine remains constant.

This output is connected to the CID_INBIT connection of the BASIC device during development. For production, the sampling stage of the CID Engine is bypassed. The CID Engine and CID Engine Interface use the same 48 kHz sample clock and are automatically synchronized, therefore, no re-sampling of the data (and associated error) is required.

When the CIDEN bit is reset to '0', the CID_DATAx and PING/PONG bits is reinitialized to '0'.

Note that if the CIDEN bit is a '1' when the LSD DATAMODE bit is a '0', the *Data2* packet will contain 16-bit received data words from the IA, and therefore the bits in the CID_DATAx fields will be invalid.

Upon receipt of the CID_DATAx data, the Caller ID Engine determines if the incoming Caller ID data is valid. If so, the Caller ID Engine will assert a PME event, waking the host system, and store up to 256 bytes of Caller ID data. This functionality is already present in the BASIC 2.15 device and will require little if any change. If the Caller ID Engine determines that the data is not valid, the DIB will be put back into Low Power Mode (140 kHz clock) and the Caller ID Engine will reset to idle state, after resetting the interrupt.

5. RING#/RINGWAKE# Generation

A description of the differences between a "classic" Ring Detect circuit, and the RDO/LPR (Ring Detect Out/Line Polarity Reversal) circuit is in order, to explain the requirements of the RING# and RINGWAKE# signals as already developed by Systems Engineering.

In the "classic" Ring Detect circuit, the ring detector consists of a bi-directional opto-isolator, and zener diodes to set the ring detect threshold. These components are AC coupled to the line via a series capacitor. If the ring signal exceeds the zener regulating voltage, the signal reaches the opto-isolator input stage. The bi-directional opto-isolator provides full-wave rectification of the signal, resulting in a square wave with fundamental frequency component at twice the ring frequency. Between rings, the opto-isolator output is inactive. Variations on this circuit, which use a unidirectional opto-isolator to produce a half wave rectified ring voltage, also exist.

The Line Side Device derives these signals from the Ring signal differently. Two sets of comparators, both AC coupled to the line, are used. The only difference between the two comparators is the reference voltage polarity. The comparators use a programmable (via a 6-bit DAC) reference voltage, which sets ring detect threshold. In this manner, the system can adapt to country specific ring voltage threshold requirements via a simple host programmable command.

5.1. Requirements

A ring voltage with AC amplitude above the programmed threshold will produce complementary half-wave rectified square waves on each comparator output with the fundamental frequency of the ring signal (nominally 20 Hz). A Line Polarity Reversal (a single step change in Tip/Ring voltage from polarity A to polarity B, or vice versa) will produce a single pulse on one comparator output or the other. A pulse dial will produce a nominal 10 Hz output from both comparators.

The comparator outputs are sampled at a 16 kHz rate by the LSD, and placed in the LSD TRSTAT register. When the DATAMODE control bit in the LSD MCR register is a '1', the TRSTAT register is copied to the Data2 and Data2bis words, replacing the received 16 bit word from the IA. Thus, the SSD can only do useful ring detection when the DATAMODE bit is a '1'. This should be the desired mode when the host system is asleep

5.2. Proposed Implementation

The Line Side Device samples the incoming analog ringing signal from both comparators (when control bit ~RD/CID in the MONADC register is a '0') at a 16 kHz rate. The resulting 1-bit samples will be placed into the LSD TRSTAT register, and if the DATAMODE bit in the LSD MCR register is a '1', the TRSTAT register will be transmitted to the SSD in the Data2 and Data2bis packets.

The SSD will begin shifting the most recently received bit from the RDO/LPR field of the TRSTAT (in Data2/Data2bis) out to the BASIC and/or data pump devices for HSF or HCF designs, respectively, using the 16 kHz clock (the same clock used for FSP generation). In the event that both the Data2 and Data2bis packets are received in error, the ring output remains constant until the next sample (frame) is received from the DIB. Note that the output should be inverted, since the BASIC device expects a RING# signal (negative active) and the LSD produces a positive active output from the comparator.

For D3Cold ring detection (and subsequent D3Cold Caller ID detection), the RING# signal from the SSD will be used by the BASIC device to produce a RINGWAKE# signal for the Caller ID Engine.

In addition to the RING# output, the RINGWAKE# generation logic in the BASIC device should be able to identify a Line Polarity Reversal for Japanese and British Caller ID reception. The Line Side Device design requires that both RDO/LPR and ~LPR be monitored to reliably detect LPR. Thus, the ~LPR output should also be shifted out to the BASIC device at each sample time (when the RDO/LPR logic is sent). A glitch on either (but not both) comparator outputs, with no further activity will indicate a large step change in voltage and can be identified as a LPR. This type of input should cause RINGWAKE# to be active low for the required time to wake the Caller ID Engine.

Note that if the DATAMODE bit is a '0', the *Data2* packet will contain 16-bit received data words from the IA, and therefore the bits in the RDO/LPR and -LPR fields will be invalid.

Upon receipt of the RING# data, and subsequent transformation to RINGWAKE# in the BASIC device, the Caller ID Engine determines if the incoming events should wake the PC via a PME event. If not, the DIB will be put back into Low Power Mode (140 kHz clock) and the Caller ID Engine will reset to idle state, after resetting the interrupt.

5.3. Development System Consideration

The CID Engine in an earlier device does not receive this ring signal directly. Rather, a secondary signal, RINGWAKE#, which is derived from RING#, may be supplied via an external comparator circuit.

In future developments, it is expected that the CID_Engine will be able to accept RING# as an input directly.

For maximum compatibility, this feature should be retained, so that future projects may use either RING# or RINGWAKE# output from the SSD as an input to other logic (such as the CID Engine).

6. Call Progress Monitor

The System Side Device logic may provide a Call Progress Monitor function. This function generally does not exist on the Line Side Device or on the LSD side of the DIB simply because of the power required to run a speaker driver.

6.1. Requirements

The SSD Call Progress Monitor provides an audible monitor output for the end user. This output will be routed to a speaker, allowing the user to monitor call progress functions such as dial tone, dialing, busy or error tones from the telephone company. Also, this circuit will allow monitoring of standard modem call progress including handshake, negotiations, and communications portions of a modem transaction, depending on the call progress AT command (ATMx) issued by the user to the system.

The Call Progress Monitor is routed to a single digital output pin. This pin will be connected to a small speaker or Sounducer, either directly or via a series RC network to filter the output as required for the system.

6.2. Proposed Implementation

This feature may use either the RXA signal from the Line Side Device, or the TXA signal from the System Side Device (or both), as a source. These signals are present in the System Side Device in the *Data2*, *Data2bis*, *Data1*, and *Data1bis* packets during each frame, if the DATAMODE bit in the LSD MCR register is a '0'.

Using RXA as a signal source implies that the output of the Call Progress Monitor will consist of the Received analog signal, plus a portion of the Transmit signal, reflected from the line interface. The magnitude of the Transmit signal for monitoring is wholly dependent on the degree of mismatch between the LSD DAA circuits and the actual telephone line

interface. Using TXA as a signal source implies that the output of the Call Progress Monitor will consist only of the Transmitted analog signal.

The output of the Call Progress Monitor will consist of the sign bit of the received 16-bit data word in the *Data2/Data2bis* or *Data1/Data1bis* packets, depending on the CPMSRC control bits. For the RXA CPM, if the output of the 16-bit sigma delta ADC in the LSD contains no DC component, and the received signal is of sufficient magnitude, CPM will consist of a waveform consisting primarily of the fundamental component of the received signal. Note that the output of the ADC in past products has generally contained a DC component. Since the TXA signal is digitally provided to the SSD from the host, it is expected to have no DC component.

If testing, prior to final System Side Device integration, reveals a better solution than the above, it should be implemented.

7. System Side Device Register Set (Proposed)

7.1. Requirements

Two types of registers exist: System Side Device registers which directly affect system side logic, and Line Side Device registers which are accessed by the System Side Device over the DIB and relayed to the host. The former can be read from or written to in one normal read/write cycle. The latter require several read/write cycles simply due to the DIB architecture and latency. Errors in transmission of data across the DIB can increase this latency in multiples of the frame clock (1/16 kHz time periods). In an ideal DIB implementation (which never experiences DIB channel errors), the maximum delay for these indirectly accessed LSD registers is 2×62.5 , or 125 microseconds.

When the host writes to a Line Side Device register, the System Side should initiate a write across the DIB. If the host is only capable of 16 bit writes, then the System Side may cache $\frac{1}{2}$ of the write, and implement the host write as two 8-bit writes across the DIB. If the host is capable of 8-bit writes (recommended), then the System Side Device can implement the write directly as one 8-bit write across the DIB. The host may then begin polling the SSD to determine if the write was completed without error. One register (LSDSTAT) will be used for feedback to the host regarding the status of such writes.

When the host reads from a Line Side Device register, the System Side initiates a read across the DIB. If the host is only capable of 16-bit reads, then the System Side may cache $\frac{1}{2}$ of the read, and implement the host read as two 8-bit reads across the DIB. If the host is capable of 8-bit reads (recommended), then the System Side Device can implement the read directly as one 8-bit read across the DIB. The host may then begin polling the SSD to determine if the read has been completed without error. If so, the host can then read the LSD shadow register a second time to get the most recently read data. This can allow frame-by-frame polling of the same LSD register by simply initiating a read, waiting until the data is ready (by polling the LSDSTAT register), then reading the new data (which initiates another read), etc.

7.2. Proposed Implementation

The following proposed implementation provides control and status functionality known to be required as of this writing.

Short Name	Reg. #	Read/ Write	Default Value (Hex)	Bits									
				D7	D6	D5	D4	D3	D2	D1	D0		
MISC	14	R/W	00	PDM	LISTEN	CID_RSS[1:0]		X	DIB FAIL	CPMSRC[1:0]			
RXDATAH	13	R	00	Current RX word, high byte (RXDATA[15:8])									
RXDATAL	12	R	00	Current RX word, low byte (RXDATA[7:0])									
TXDATAH	11	R/W	00	Current TX word, high byte (TXDATA[15:8])									
TXDATAL	10	R/W	00	Current TX word, low byte (TXDATA[7:0])									
CIDENGCTL	0F	R ⁰	00	CIDEN	CID_DATA2[2:0]			PING/ PONG	CID_DATA1[2:0]				
ERRRETRY	0E	R ⁽¹⁾	00	Counter[7:4]				Counter[3:0]					
ERRSYNC	0D	R ⁽¹⁾	00	Counter[7:4]				Counter[3:0]					
ERRD2b	0C	R ⁽¹⁾	00	Counter[7:4]				Counter[3:0]					
ERRCNTL2	0B	R ⁽¹⁾	00	Counter[7:4]				Counter[3:0]					
ERRD2	0A	R ⁽¹⁾	00	Counter[7:4]				Counter[3:0]					
ERRD1b	09	R ⁽¹⁾	00	Counter[7:4]				Counter[3:0]					
ERRCNTL1	08	R ⁽¹⁾	00	Counter[7:4]				Counter[3:0]					
ERRD1	07	R ⁽¹⁾	00	Counter[7:4]				Counter[3:0]					
CLKPWR	06	R/W	08	CLKEN	PWROUT[2:0]			FREQ	CLKSHIGH[2:0]				
IMASK	05	R/W	00	X	X	X	X	X	ERR FULLM	LSD GPIOM	CNTL RDYM		
ISRC	04	R/W	00	X	X	X	X	X	ERR FULLA	LSD GPIOA	CNTL RDOYA		
LSDADDR	03	R/W	00	W/R	ADDR[5:0]							H/L	
CNTLOUT	02	R/W	00	CONTROLOUT[7:0]									
CNTLIN	01	R	00	CONTROLIN[7:0]									
LSDSTAT	00	R/W	00	INT	INTE	FINI	OK	X	RX	TX	WAIT		

Notes:

(1) Error Counter registers (06h through 0Dh) are automatically incremented by the SSD, and functionally read-only. Any write to an error counter register will reset the particular error counter register to 00h.

(2) The SSD Caller ID Engine Control register is read-only except for bit 7 (CIDEN), which is read/write capable. A write to bit 7 resets bits 6 through 0 to '0'.

All bits shown in dark gray are not required in the first device and need not be implemented. Such bits are placeholders in the specification for expected future expansion.

7.2.1. System Side Device Register Bit Definitions

Name	Reg.	Def.	Description
ADDR	03:[6:1]	00h	DIB Control1 packet, 6-bit Address field.
CID_DATA1	0F:[2:0]	000	CID Data Buffer 1. Contains 3-bit CID Data from the Data2/Data2bis packet to be shifted to the Caller ID Engine one bit at a time. See Section 7.2.2 for a full description of the CID Data buffering scheme.
CID_DATA2	0F:[6:4]	000	CID Data Buffer 2. Contains 3-bit CID Data from the Data2/Data2bis packet to be shifted to the Caller ID Engine one bit at a time. See Section 7.2.2 for a full description of the CID Data buffering scheme.
CID_RSS	14:[5:4]	00	Caller ID Engine RingSizeSelector control bits, moved from BASIC P85 ring logic.
CIDEN	0F:7	0	Caller ID output enable. Control bit CIDEN enables the output of CID_DATA bits to the CID_INBIT input of the CID Engine in the BASIC device. '1' = Caller ID Data shifted out to the CID_INBIT input of the BASIC device at 1-bit per 48 kHz clock. '0' = Caller ID Data not shifted to the CID Engine.
CLKEN	06:7	0	Clock Enable. The CLKEN control bit controls the output drivers of the differential master clock/power source for the Line Side Device. '1' = Differential clock drivers enabled. '0' = Differential clock drivers disabled (pulled low).
CLKSHIGH	06:[2:0]	000	Clocks High. Control bits CLOCKSHIGH control the duty cycle of the output clock/power. '000' or '111' = 50% duty cycle. '001'-'110' = 1 to 6 7ths high, 6 to 1 7ths low. This control can be used to control the total amount of power delivered to the LSD.
CNTRLRDA	04:0	0	Control Channel Ready Interrupt Active. '1' = DIB Ping/Pong complete (either bit ERR or bit OK is a '1'). Control channel ready for next access. '0' = DIB Ping/Pong Incomplete. Control channel busy.
CNTRLRDY	05:0	0	Control Channel Ready Interrupt Mask. '1' = Interrupt active. '0' = Interrupt inactive (unable to generate host interrupt).
CONTROLIN	01:[7:0]	00h	DIB Control2 packet, 8-bit Control field. Contains 8-bit byte that was received from LSD register.

CONTROL OUT	02:[7:0]	00h	DIB Control1 packet, 8-bit Control field. Contains 8-bit byte to be read or written to or from LSD register.
CPMSRC[1:0]	14:[1:0]	00	System Side Device Call Progress Monitor source select control. '00' = CPM digital output inactive (clamp to high). '01' = CPM digital output contains MSb from RXA word. '10' = CPM digital output contains MSb from TXA word. '11' = CPM digital output contains RXA MSb logically OR'd with TXA MSb.
DIBFAIL	14:2	0	DIB Failure Status Indicator. Indicates when one of the Error Counters has reached maximum value (for 4-bit counters, indicates when any of the 8 error counters reaches 'F'). May be used as an interrupt. See ERRFULLM and ERRFULLA.
ERRCNTL1	08:[7:0]	00h	Control1 packet error counter. Automatically incremented by SSD each time bit ERR of Control2 packet is a '1'. Reset to zero by any host write.
ERRCNTL2	08:[7:0]	00h	Control2 packet error counter. Automatically incremented (and SSD bit ERR(00:5) is set to '1') by SSD each Data2 packet has parity or non-legal symbol error. Reset to zero by any host write.
ERRD1	07:[7:0]	00h	Data1 packet error counter. Automatically incremented by SSD each time bit ERR of Data2 packet is a '1'. Reset to zero by any host write.
ERRD1b	09:[7:0]	00h	Data1bis packet error counter. Automatically incremented by SSD each time bit ERR of Data2bis packet is a '1'. Reset to zero by any host write.
ERRD2	0A:[7:0]	00h	Data2 packet error counter. Automatically incremented by SSD each Data2 packet has parity or non-legal symbol error. Reset to zero by any host write.
ERRD2b	0C:[7:0]	00h	Data2bis packet error counter. Automatically incremented by SSD each Data2bis packet has parity or non-legal symbol error. Reset to zero by any host write.
ERRFULLA	04:2	0	Error Counter Full Interrupt Active indicator. '1' = One of the 8 error counters has reached the maximum allowed value ('F' for 4-bit counters). '0' = Error Counters are all below maximum value.
ERRFULLM	05:2	0	Error Counter Full Interrupt Mask. '1' = Interrupt active. '0' = Interrupt inactive (unable to generate host interrupt).

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ERRRETRY	0E:[7:0]	00h	DIB Re-synchronization retry counter. Each time the SSD attempts to re-synchronize with the LSD, a failure of the LSD to reply to a SSD frame within 5 symbol clocks causes the SSD to auto-increment this counter and retry. Reset to zero by any host write.
ERRSYNC	0D:[7:0]	00h	DIB Synchronization error counter. Each time the LSD loses synchronization with the SSD and fails to transmit Data2, Control2, and Data2bis packets to the SSD, the SSD auto-increments this counter and begins trying to re-synchronize with the LSD. Reset to zero by any host write.
FINI	00:5	0	DIB Protocol status indicator. '0' = Waiting for packets to be received from LSD, or DIB in 'Listen Mode'. '1' = Data2, Control2, (and opt. Data2bis) packets received from LSD and decoded. (May be used as interrupt source for host. The bit will be reset when the host writes a '0' to this bit.)
FREQ	06:3	1	Frequency. Control bit FREQ controls the output frequency of the differential clock outputs. '1' = 4 MHz output frequency. '0' = 140 kHz output frequency. (LSD 'asleep')
H/L	03:0	0	DIB Control1 packet, H/L control bit. '1' = High – access upper half of 16-bit LSD register. '0' = Low – access lower half of 16-bit LSD register.
INT	00:7	0	Copy of the MSb of the Control2 packet. Indicates the current interrupt status of the Line Side Device GPI.
INTE	00:6	0	Hardware Interrupt output enable for the SSD logic. '0' = Interrupt output not driven. '1' = Interrupt output driven.
LISTEN	14:6	0	System Side Device DIB state control. When the 4 MHz clock is active, if the LISTEN bit is: '0' = DIB if is in Protocol Mode, sending and receiving frames over the DIB every 16 kHz sample time. '1' = DIB interface is in Listen Mode, awaiting an interrupt (FSP) from the LSD.
LSDGPIOA	04:1	0	Line Side Device GPIO Interrupt Active Indicator. '1' = LSD GPIO interrupt is currently active. '0' = No Interrupt from LSD GPIO. Note: Copy of bit INT(00:7).
LSDGIOM	05:1	0	Line Side Device GPIO Interrupt Mask. '1' = Interrupt active. '0' = Interrupt inactive (unable to generate host interrupt).
OK	00:4	0	Status indicator for Control2 packet. This bit is reset when the host writes to the LSDADDR register. '0' = Control2 packet received with error (if FINI = 1) or not yet received. '1' = Control2 packet received without error.

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PDM	14:7	0	Control bit to select Parallel Data Mode for data channel. '0' = Serial Data Mode. Data to and from LSD is passed to and from SSD via a 20410-type SIF. Data words are echoed to SSD registers \$10-\$13, which are read only in this mode. '1' = Parallel Data Mode. Data to and from LSD is passed to and from SSD via parallel bus, to registers \$10-\$13. Registers \$10-\$11 are R/W, and \$12-\$13 are read only.
PING/PONG	0F:3	0	CID Data PING/PONG buffer indicator. Indicates which of the two CID_DATAx buffers contains the most recent 3-bit input from the DIB. '1' = CID_DATA1[2:0] contains the most recently read CID data. CID_DATA2 will be over-written when the next 3-bit data is received. '0' = CID_DATA2[2:0] contains the most recently read CID data. CID_DATA1 will be over-written when the next 3-bit data is received. PING/PONG is automatically toggled when the latest 3-bits are received from the DIB and placed into CID_DATAx.
PWROUT	06:[6:4]	000	Power Output control. Controls the drive current of the differential clock output drivers.
RX	00:2	0	DIB Receive Status indicator bit. '0' = DIB ping/pong protocol not in RX state. '1' = DIB ping/pong protocol in RX state, receiving bits 64-117.
RXDATAH	13:[7:0]	00h	Receive Data High. Upper half of 16-bit received data word, from Data2/Data2bis packets. (Parallel data mode only).
RXDATAL	12:[7:0]	00h	Receive Data Low. Lower half of 16-bit received data word, from Data2/Data2bis packets. (Parallel data mode only).
TX	00:1	0	DIB Transmit Status indicator bit. '0' = DIB ping/pong protocol not in TX state. '1' = DIB ping/pong protocol in TX state, transmitting bits 0-61.
TXDATAH	11:[7:0]	00h	Transmit Data High. Upper half of 16-bit transmit data word, for use in Data1/Data1bis packets. (Parallel data mode only).
TXDATAL	10:[7:0]	00h	Transmit Data Low. Lower half of 16-bit transmit data word, for use in Data1/Data1bis packets. (Parallel data mode only).
W/R	03:7	0	DIB Control1 packet, W/R-bit. '1' = Write. '0' = Read.
WAIT	00:0	0	DIB Waiting for next ping/pong indicator bit. '0' = DIB ping/pong protocol not waiting. '1' = DIB ping/pong protocol waiting until next 16 kHz frame to begin to shift requested LSDCNTL.

7.2.2. Caller ID Ping/Pong Buffer

Since 3 bits are transferred from the Line Side Device at a time, it will be useful to buffer 3-bit reads in case a new read is performed before all three bits are clocked out to the Caller ID Engine from the last 3-bit read. It is possible to implement a simple ping/pong buffer inside the CIDENGCTL register itself, as follows:

By default, the PING/PONG bit will be '0'. Setting the CIDE bit to '1' (or any write to the CIDENGCTL register), will reset the PING/PONG bit (and the two 3-bit CID_DATAx fields) to '0'.

When CIDE is a '1', *Data2/Data2bis* packet bits [10:8] will be copied to the CIDENGCTL register and shifted out at a 48 kHz clock rate to the CID_INBIT input of the CID Engine ASIC logic. Bit 10 is the oldest 1-bit CID comparator output sample.

When a new *Data2/Data2bis* packet is received, if PING/PONG is a '0', then:

- (1) Bits [10:8] of the Data packet will be copied to bits [2:0] of CIDENGCTL (called CID_DATA1[2:0]), and
- (2) PING/PONG will be set to a '1' automatically.
- (3) [SSD or host can now use CID_DATA1 bits].

Likewise, when a new *Data2/Data2bis* packet is received, if PING/PONG is a '1', then:

- (1) Bits [10:8] of the Data packet will be copied to bits [6:4] of CIDENGCTL (called CID_DATA2[2:0]), and
- (2) PING/PONG will be reset to a '0' automatically.
- (3) [SSD or host can now use CID_DATA1 bits].

When CIDE is a '0', no output should be provided from the SSD logic to the CID Engine CID_INBIT. Bits 6 through 0 of CIDENGCTL are invalid for CID use.

7.3. Line Side Device Registers

The Line Side Device includes the registers shown below. Note that these are accessed via the LSDSTAT, LSDDATA, and LSDCNTRL registers indirectly over the DIB only, with one exception. When the DATAMODE bit of the LSD MCR register is a '1', the *Data2* and *Data2bis* packets contain the TRSTAT register contents instead of the sigma delta ADC RX word during each frame.

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Short Name	8-bit Register #	Bits															
		D15	D14	D13	D12	D11	D10	D9	D8	D7	D6	D5	D4	D3	D2	D1	D0
NULL	00	X	X	X	X	X	X	X	X	X	X	X	X	X	X	X	X
EXUSC*	01	X	X	X	X	PRD	PRC	PRB	PRA	X	X	X	X	DAC1	ADC1	Mref	GPIO
MIR	02	X	X	X	X	X	X	X	X	SR[7:0]							
MIL	03	Mult DAC	X	X	X	DAC3	DAC2	DAC1	DAC0	Mult ADC	X	X	X	ADC3	ADC2	ADC1	ADC0
GPIOC	04	GC[15:0]															
GPPOP	05	GP[15:0]															
GPIOsti	06	GCS[15:0]															
GPLOW	07	GW[15:0]															
GPPOS	08	GI[15:0]															
GPPOD	09	GD[15:0]															
MCR*	DA	TXM	-OH	DM1	DATA MODE	RX GAIN	L1B2	L1B1	L1B0	LM11	LM10	SCM1	VM11	VM10	AM1	EIO3	X
MONADC	0B	RDY	LCL	<MSB>	ADC[5:0]				<LSB>	-RD/ CID	X	ADSEL[1:0]					X
DCDAC	0C	X	X	<MSB>	DAC[5:0] (write only)				<LSB>	X	DASEL[25:0]				WZ2	WZ1	USZ1

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TRSTAT	00	X	VCR2:1	VCR	X	CID_DATA2:0	X	-LPR(2:1)	-LPR	X	RDO/LPR2:1	RDO/LPR
-	0E	X										
TEST*	0F	TEST[15:0] Reserved for Test										
VEN1*	10	X	X	X	X	X	X	Bond1	Bond0	Rev[5:0]		

* Registers which require 3 successive writes or reads without intermediate writes or reads from other registers to effect a change. This is to prevent these registers from being accidentally changed, which would power down the device or reset the registers.

Notes:

- (1) CID_DATA[2] is the oldest of the three 1-bit Caller ID samples.
- (2) For interrupt generation (wake-up) purposes, the LCL status bit which indicates when the LSD experiences an unexpected loss of line current, is mapped to GPIO0. The RING comparator output (RDO/LPR) is mapped to GPIO1, the -LPR comparator output is mapped to GPIO2, and the VCR output is mapped to GPIO3. Transitions on any of these bits should cause the Line Side Device (when asleep) to send an alerting signal to the System Side Device, causing the System Side Device to wake up the Line Side Device and handle the event (Caller ID, or Ring).
- (3) Bits shown with no shading, and denoted by 'X', need not actually be implemented in the production device. They should have no effect when written to, and should return '0' when read. Bits shown in dark gray may be omitted from the first production device. The DIB protocol should be robust enough to support 16 GPIO bits as discussed in the PRS. However, the device requires only 4 GPIO. Similarly, the 2nd and 3rd bits for VCR, RDO/LPR, and -LPR are for future use and do not need to be implemented in the first device.
- (4) Register 0 is reserved as a null register, to be used for all Control packets where a valid register is not referenced.
- (5) Registers 1 through 8 are defined in the 20424 Specification, and consist of all modem-specific registers inside the AMC97 codec. Register 9 is simply a GPIO Data Register, which contains the current GPIO values, and may be read/written to. Register A is a combination of AMC97 registers MISM and MCR1, and special control bits.

- (6) Registers B through D consist of all specific control and status registers. These registers will be mapped to reserved registers 62h-66h in an AMC97 application by the SSD.
- (7) Register F is reserved for test controls.
- (8) Register 10 contains a 6-bit revision code to identify the LSD, as well as 2 bonding option status bits that will be defined later. Note that bonding options should be implemented such that the presence of a bonding wire enables the option, preventing unauthorized or surreptitious enabling of features by removing wires after packaging. Writing to this register resets all register bits to default values.
- (9) ADSEL options will be decoded to 1 of 4 selections, based on the 2 ADSEL bits.

8. Line Side Circuitry

The Line Side device of this implementation contains the following list of functional blocks.

- 2nd order Sigma-Delta Codec (modem ADC/DAC channel)
- Electronic Inductor
- World Wide Impedance
- Ring Detector
- Caller ID Detector
- Hook Switch/Pulse Dialer
- Extension Off-Hook Detector
- GPIO
- 6-bit DAC
- 7-bit ADC

The following sections will describe an embodiment of the Line Side device primarily from the DIB Interface. Therefore, these sections will describe the data protocol to be used on the DIB to send and receive data, control, and status information and list required control registers, describe each control function, list status registers, describe each status function, and list and describe Codec registers.

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9. DIB Protocol – Line Side

9.1. Requirements

The DIB protocol passes all required register data over the Digital Isolation Barrier, including, at minimum, one Transmit and one Receive Data Word per 16 kHz sample time, and optional control/status words. A means of re-transmitting packets received in error may be implemented since no error correction exists at the receiver.

This DIB Protocol discussion concentrates on a description of Line Side device behavior. For a complementary discussion of System Side behavior, see the System Side Device Digital Functional Specification.

9.2. Proposed Implementation

9.2.1. Assumptions

The Line Side implementation of the DIB protocol assumes the following:

- The Line-Side Device (LSD) is a slave device to the System Side Device (SSD). The LSD does not initiate a transfer across the DIB unless it is requested, except when asleep.

Note: This implies that any semi-continuous monitoring of Line Side status by the System Side requires the System Side to poll the LSD.

- The Line Side Device will only communicate over the DIB to the System Side Device using the DIB packet protocol when both are awake (i.e., 4 MHz clock is running), and the Line Side has been synchronized to the System Side.
- The Line Side Device will go to 'listen' mode and await GPIO activity or SSD resynchronization when no FSP frame is received from the SSD.
- The System Side Device should write to the power control register (EXMSC, Register 000001) to power down portions of the Line Side Device prior to reducing the clock frequency. In sleep mode, GPIO states may be maintained and the Caller ID and Ring detectors may function.
- When asleep, the Line Side Device will generate a wake-up signal across the DIB to the System Side Device if any activity is detected by the Ring detector, Caller ID detector, or GPI.

Note: Obviously non-legal states (such as going off-hook without being commanded to do so or while asleep) should cause the Line Side device to generate a wake-up signal across the DIB to the System Side Device.

- Once synchronization is established across the DIB, both sides can count clock cycles (of the 4 MHz input clock, or the 2 MHz clock derived from it).

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- It takes less than one (2) 2 MHz clock cycles for the DIB transceivers to switch from one direction to another. Two information bit times are allocated every time the direction of communication is changed.
- The Line Side device is not responsible for analysis of the RING signal, including Pulse Dial rejection, Extension off-hook rejection, RING_WAKE generation, or RING verification. The System Side Device is responsible for these functions.

9.2.2. Bandwidth Summary

See section 2.2.2.

9.2.3. DIB Ping-Pong Protocol Summary

See section 2.2.3

9.2.4. Frame Synchronization Pattern Definition

See section 2.2.4

9.2.5. Reversal Synchronization Pattern Definition

See section 2.2.5

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Packet Definitions

The following sections show the format for each of the packets received by or sent by the Line Side device. The packets are shifted over the DIB from left to right as shown in the tables below, ending with the parity bit.

For simplicity, all packets consist of 18 bits and end with a single parity bit.

9.2.5.1. Packets Received by the Line Side Device

9.2.5.1.1. Data1 Packet Definition

Data		---	PAR
<MSb>	16 bits	<LSb>	1 bit

- DATA: 16-bit sample, with the most significant bit shifted first.
- PARITY (PAR): Parity bit, used for error detection. Odd parity will be calculated using the first 16 bits of the packet.

9.2.5.1.2. Control1 Packet Definition

W/R	Address	H/L	Control	---	PAR
1 bit	6 bits	1 bit	8 bits	1 bit	1 bit

- WRITE/READ (W/R): In a control packet sent by the system side, this bit indicates whether this is a write or a read request. W/R is set to '1' for a write request, to '0' otherwise.

Note that for a read request, the system side device sends a packet with null control bits, used to pad the control packet to the full 18 bits.
- ADDRESS: This field contains the address of the control/status register being transmitted.
- HIGH/LOW (H/L): Control bit used to indicate whether the SSD is addressing the upper (high) or lower (low) byte of the 16-bit LSD register. This bit is set to '1' if the high byte is being addressed, to '0' otherwise.

Note: The Line Side Device DIB interface implements logical 8-bit addressing using the Address (6-bit) and H/L bit. The high or low byte is transmitted independently of the other byte (i.e., it is not necessary for the host to follow the high byte with the low byte or vice versa).
- CONTROL: This field contains the control/status byte.
- PARITY (PAR): This bit is a parity bit, used for error detection. Odd parity will be calculated using the first 17 bits of the packet.

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9.2.5.1.3. Data1bis Packet Definition

The contents of the *Data1bis* packet are identical to those of the *Data1* packet.

9.2.5.2. Packets Transmitted by the Line Side Device

9.2.5.2.1. Data2 Packet Definition

Data		ERR	PAR
<MSb>	16 bits	<LSb>	1 bit

- **ERROR (ERR):** The Line Side device sets this bit if an error was detected in the received *Data1* packet from the System Side device.

A counter should be implemented on the System Side device to track how many times the Line Side indicates an error in transmitted data packets. The host should be able to reset the counter on demand.

- **DATA:** 16-bit sample, with the most significant bit shifted first. When control bit DATAMODE in the Line Side Device register MCR is a 1, the Data will consist of the sampled output of the Caller ID comparator and the RING comparators, in the following format. For Caller ID and RING, the 3 bits represent 3 1-bit comparator outputs sampled at 48 kHz. The most significant bit of each field is the 'oldest' bit. Caller ID data and RING data are also available via polling Register C1.

D15	D14	D13	D12	D11	D10	D9	D8	D7	D6	D5	D4	D3	D2	D1	D0
0	VCR[2:0]			0	CID DATA[2:0]			0	-LPR[2:0]			0	RDO/LPR[2:0]		

- **PARITY (PAR):** This bit is a parity bit, used for error detection. Odd parity will be calculated using the first 17 bits of the packet.

9.2.5.2.2. Control2 Packet Definition

INT	Address	H/L	Control	ERR	PAR
1 bit	6 bits	1 bit	8 bits	1 bit	1 bit

- **INTERRUPT (INT):** The Line Side device sets this bit when an "Interrupt" event occurs in the Line Side device register set.

Note that only GPIO registers can generate interrupts. GPIO interrupts can be level ('0' or '1') or edge (rising or falling) generated, as defined in the AMC97 GPIO register control set definition. See the 20424 Specification for more details. The output of the RDO/LPR and -LPR comparators should be connected to GPIO on the Line Side Device and programmed by the SSD to generate interrupts based on any ring activity. After an Interrupt is signaled in the Control2 packet, the System Side Device will most likely read the GPIO Status register in the following frame to identify the Interrupt source.

- ADDRESS: This field contains the address of the control/status register being transmitted. In the case of a write, the address written to is echoed back to the System Side Device.
- HIGH/LOW (H/L): Control bit used to indicate whether the LSD is returning the upper (high) or lower (low) byte of a 16-bit LSD register. This bit is set to '1' if the high byte is being addressed, to '0' otherwise.

Note: The Line Side Device DIB interface implements logical 8-bit addressing using the Address (8-bit) and H/L bit. The high or low byte is transmitted independently of the other byte (i.e., it is not necessary for the host to follow the high byte with the low byte or vice versa).

- CONTROL: This field contains the control/status byte. In the case of a response to a write, the control byte written to the Line Side Device is echoed back to the System Side Device.
- ERROR (ERR): The Line Side device sets this bit if an error was detected in the received *Control1* packet from the System Side device.

A counter should be implemented on the System Side device to track how many times the line side indicates an error in transmitted control packet. Note that an erroneously received control packet will be discarded by the Line Side and should be retransmitted at the next frame. The host should be able to reset the counter on demand.

- PARITY (PAR): This bit is a parity bit, used for error detection. Odd parity will be calculated using the first 17 bits of the packet.

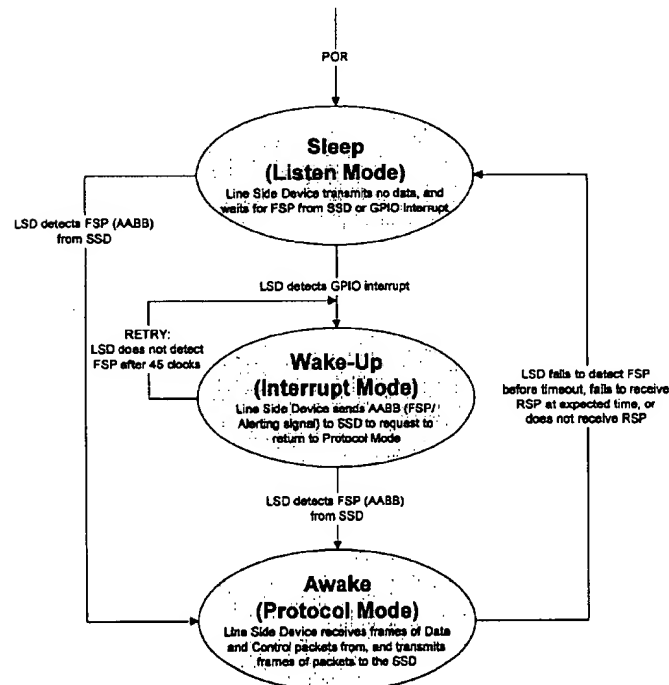
9.2.5.2.3. Data2bis Packet Definition

The contents of the *Data2bis* packet are identical to those of the *Data2* packet. The only difference is that the ERR bit is only set if the LSD detected an error in the *Data1bis* packet received.

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10. DIB Synchronization – Line Side

Synchronization will be achieved/maintained between the SSD (master) and LSD (slave) by means of a special sequence of symbols (the FSP) sent to the Line Side device at the beginning of each frame or whenever synchronization is lost. When sufficient power is present (i.e., the power clock is being received), the LSD will always respond to a frame beginning with the FSP. When power is present, but the LSD is 'asleep', GPIO activity will cause the LSD to send FSP to the SSD, to request wake-up. A state-diagram is included in Figure 2 below:



• Figure 2. Line Side Device DIB States

10.1. DIB Power On Reset

When the system is powered up, the Line Side DIB interface defaults to Listen Mode, in which it is a receiver, awaiting a frame of data and control information from the SSD. The

System Side device initiates normal operation (Protocol Mode) by sending a frame of data and control information to the LSD. Each time it completes transmission of the frame, the system side reverses the DIB and "listens" for the return packets from the LSD. If it does not receive anything within the following 5 bit times, it reverses the DIB again and re-transmits the frame.

The periodic re-transmission of the frame continues until the Line Side successfully receives the full frame. When the LSD detects the end of a full frame, the LSD configures its DIB interface as an output and begins transmitting the return packets within 5 bit times of the end of the SSD RSP. After the SSD successfully receives the return packets from the LSD, normal communication between the two devices has been established, and the SSD will send periodic frames to the LSD.

10.1.1. Cold Reset

The System Side Device may at any time perform a cold reset of the LSD by stopping the power clock altogether for a predetermined number milliseconds, allowing the VCC voltage of the LSD to dissipate. The System Side may then re-start the Line Side Device by turning on the clock and performing the synchronization described above. This reset mechanism is slow and should be used only as a last resort. Alternatively, the System Side Device may write to the ID register (VEN1, Register 16) to reset all register bits to default status.

10.2. Line Side Wake-Up Summary

If the Line Side is 'asleep' (i.e., the device is in Listen Mode and the power clock is 140 kHz) and activity is detected from any GPIO configured to generate an interrupt, the Line Side will generate an alerting signal to the System Side Device. Immediately after alerting the SSD, the LSD will switch its interface to receive mode.

The alerting signal will consist of 4 symbols, 'AABB', at the 70 kHz bit rate (1/2 the power clock). This will correspond to data bits of '11110000'. Note that 'A' and 'B' have been chosen as noise tolerant special signals because they generate a transmit signal which is a sub harmonic of the 140 kHz power clock and the 70 kHz bit clock and will therefore be unlikely to be generated by board or clock noise.

Upon detection of the activity on the DIB data lines, and verification of the 'AABB' signal, the System Side device will raise the power clock frequency to 4 MHz, and begin transmitting a frame beginning with FSP, as described in Section 10.1.

10.2.1. Wake-Up Time Budget

Caller ID response time appears to place the most stringent requirements on device wake-up, especially in the D3Cold case (host CPU is asleep, power is limited to the PCI slot). The Caller ID requirements generally specify a worst case time of 100 milliseconds between the alerting signal (a Line Polarity Reversal in the worst case) and the beginning of the Caller ID data. Thus, it is required that the maximum wake-up and resynchronization time for the Line Side device and DIB interface be well within the 100-millisecond limitation.

The 'AABB' System Side Device alerting signal takes approximately 60 microseconds for the Line Side to transmit. It is estimated that the output power clock on the SSD will take less than 100 microseconds to slew between the 140 kHz sleep clock and the 4 MHz

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normal operation clock. Power is already present at the Line Side Device when the 140 kHz clock is present, so no additional time is required for the Line Side power supply to ramp up. Thus, it appears that ample time is available to wake up and start receiving RING or CID_DATA for the Caller ID engine in the SSD.

10.3. Line Side Error Detection

The Line Side can detect several types of error in the received data, described below. In some cases, the Line Side response to an error is to stop communicating with the System Side device. This indicates that the System Side device should re-awaken the Line Side device with a frame beginning with FSP.

10.3.1. Non-Legal Data Symbols

If the Line Side receives an 'A' or 'B' signal at any time after the reception of the FSP, one of two types of errors has occurred. Either one half of one symbol ('0' = '01' or '1' = '10') has been corrupted, resulting in a half-symbol error, or there has been a loss of synchronization due to a clock slip on the system side device.

The Line Side device will determine which error has occurred if the RSP is received as scheduled in the protocol. If the RSP is received late or not at all, then the LSD will respond to the error by going to Listen Mode until the SSD sends another frame beginning with FSP.

If the RSP is received on time, the Line Side device detects a Non-Legal Data Symbol error, and communication over the DIB continues without a resynchronization. The Line Side device reacts by using the other data packet or discarding the control packet, as appropriate, and sets the appropriate ERR bit in its frame response.

10.3.2. Parity Error

If, at the end of the *Data1*, *Control1*, or *Data1bis* packets, the Parity bit for the first 17 bits in the packet does not agree with the LSD calculated parity of the data in the packet, then a Parity Error is detected. A Parity error in this case indicates that an odd number of symbols have changed from '0' to '1' or vice versa.

If the Parity bit of any packet is received as an 'A' or 'B' symbol, it is corrupted and the Line Side detects a Non-Legal Data Symbol error.

The Line Side Device reacts by using the other data packet or discarding the control packet, as appropriate, and sets the appropriate ERR bit in its frame response.

10.3.3. Time Out

If the Line Side device does not receive the RSP as symbols 58-61 (or alternatively 40-43) in a given frame, a loss of synchronization has occurred between the two devices. In this case, the Line Side device will enter Listen Mode until the System Side sends another frame beginning with FSP.

During the Wake Up sequence described in Section 10.2, it is possible for the System Side device to miss the Line Side alerting signal, 'AABB'. In this case, the Line Side Device should wait a number of clock cycles, and re-transmit the alerting signal. It is important that the LSD and SSD do not wait the same number of clock cycles (4 cycles of the 2 MHz

bit clock) before re-transmission, to prevent repeated collisions on the DIB of the SSD FSP and the LSD Alerting signal (FSP), and subsequent failure to wake up.

The Line Side device should still receive the 140 kHz 'sleep' clock. Therefore, each 'clock' on the Line Side corresponds to 29 clocks on the System Side (which still has the 4 MHz source). It will take less than 100 microseconds to raise the clock, and each 70 kHz clock is about 14 microseconds. Therefore, it will take a minimum of 7 clocks before the SSD frame can be sent and recognized by the LSD.

The Line Side Device should wait 45 clocks before resending the alerting signal if the SSD has not yet begun sending the FSP.

10.3.4. Error Condition Pseudo-Code

The following pieces of pseudo-code show how the Line Side Implementation of the DIB protocol handles various error conditions.

```

If (line side detects error in Data1) then
  Line side disregards data sample received in Data1;
  Line side uses data sample in Data1bis instead;
  Line side sets ERR in Data2;
Endif

If (line side detects error in Data1bis) then
  Line side sets ERR in Data2bis;
Endif

If (line side detects error in Control1) then
  Line side sends null control packet in Control2;
  Line side sets ERR in Control2;
  System side resends control packet in Control1 of the following frame;
Endif

If (line side loses synchronization (loss of clock, no FSP, etc...))
  Line side stops transmission;
  System side detects loss of contact;
  System side re-transmits frame;
  Line side detects FSP;
  Communication resumes;
Endif

```

11. Line Side Device Register Set (Proposed)

11.1. Requirements

The proposed Register Set will allow extra, unused, control and status bits for foreseeable Line Side control and status functions that are not implemented in the first design.

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11.2. Proposed Implementation

The following proposed implementation provides the control and status functionality known to be required as of this writing. In addition, the registers are structured so as to require minimal re-mapping when used in related products.

Short Name	6-bit Register #	Bits															
		D15	D14	D13	D12	D11	D10	D9	D8	D7	D6	D5	D4	D3	D2	D1	D0
NULL	00	X	X	X	X	X	X	X	X	X	X	X	X	X	X	X	X
EXMSC	01	X	X	X	X	PRD	PRC	PRB	FRA	X	X	X	X	DAC1	ADC1	Mref	GPIO
MIR	02	X	X	X	X	X	X	X	X	SR7[0]							
MIL	03	Mute DAC	X	X	X	DAC3	DAC2	DAC1	DAC0	Mute ADC	X	X	X	ADC3	ADC2	ADC1	ADC0
GPIOC	04	GC[15:0]															
GPPOP	05	GP[15:0]															
GPPOsl	06	GCS[15:0]															
GPLOW	07	GWM[15:0]															
GPLOS	08	GI[15:0]															
GPLOD	09	GD[15:0]															
MCR*	0A	TXM	-OH	DM1	DATA MODE	RX GAIN	L1B2	L1B1	L1B0	LM11	LM10	SCM1	VM11	VM10	AM1	X	X

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MONADC	0B	RDY	<MSb>		ADC[6:0]		<LSb>		-RDY CID	X	ADSEL[1:0]		X	X	X	X
DCCDAC	0C	USZ1	USZ0	<MSb>	DAC[5:0] (write only)		<LSb>		EIC0	DASEL[2:0]		X		WZ2	WZ1	WZ0
TRSTAT	0D	X	VCR[2:0]		X	CID_DATA[2:0]		X	-LPR[2:1]		-LPR		X	ROOLPR[2:1]		ROOLPR
-	0E	X														
TEST1	0F	TEST1[15:0] Reserved for Test														
TEST2	10	TEST2[15:0] Reserved for Test														
VEN1*	11	X	X	X	X	X	X	X	X	Bond0	Bond1	Rev[5:0]				

* Registers which require 3 successive writes or reads without intermediate writes or reads from other registers to effect a change. This is to prevent these registers from being accidentally changed, which would power down the device or reset the registers.

Notes:

- (1) CID_DATA[2] is the oldest of the three 1-bit Caller ID samples.
- (2) For interrupt generation (wake-up) purposes, the LCL status bit, which indicates when the LSD experiences an unexpected loss of line current, is mapped to GPIO0. The RING comparator output (RDO/LPR) is mapped to GPIO1, the -LPR comparator output is mapped to GPIO2, and the VCR output is mapped to GPIO3. Transitions on any of these bits should cause the Line Side Device (when asleep) to send an alerting signal to the System Side Device, causing the System Side Device to wake up the Line Side Device and handle the event (Caller ID, or Ring).
- (3) Bits shown with no shading, and denoted by 'X', need not actually be implemented in the production device. They should have no effect when written to, and should return '0' when read. Bits shown in dark gray may be omitted from the first production device. The DIB protocol should be robust enough to support 16 GPIO bits as discussed in the PRS. However, the device requires only 4 GPIO. Similarly, the 2nd and 3rd bits for VCR, RDO/LPR, and -LPR are for future use and do not need to be implemented in the initial device.
- (4) Register 0 is reserved as a null register, to be used for all Control packets where a valid register is not referenced.
- (5) Registers 1 through 8 consist of all modem-specific registers inside the codec. Register 9 is simply a GPIO Data Register, which contains the current GPIO values, and may be read/written to. Register A is a combination of registers MISM and MCR1 from another design, and special control bits.
- (6) Registers B through D consist of all design specific control and status registers.
- (7) Register F is reserved.
- (8) Register 10 contains a 6-bit revision code to identify the LSD, as well as 2 bonding option status bits that will be defined later. Note that bonding options should be implemented such that the presence of a bonding wire enables the option, preventing unauthorized or surreptitious enabling of features by removing wires after packaging. Writing to this register resets all register bits to default values.
- (9) ADSEL options will be decoded to 1 of 4 selections, based on the 2 ADSEL bits.

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11.2.1. Line Side Device Register Bit Definitions

Name	Reg	Def.	Description
ADC[3:0]	03:[3:0]	0	Controls signal gain to ADC in 4 steps: 0, +10, +15, +22.5 dB.
ADC[6:0]	0B:[14:8]	X	7-bit monitor ADC used for Line Voltage (on and off hook) and Vdd measurement.
ADC1	01:2	X	16-bit Sigma Delta ADC circuit ready indicator at cold start/reset. '1' = ADC ready. '0' = ADC not ready.
ADSEL[1:0]	0B:[5:4]	00	7-bit monitor ADC input select. '00' = On-hook Line Voltage. '01' = Off-hook line voltage. '10' = Vdd measurement '11' = Undefined.
AM1	0A:2	0	Modem Line ADC LPF dB gain. '0' = 0 dB. '1' = -4 dB.
Bond[1:0]	11:[7:6]	11	Bond options '0' = enable bond-able feature (add wire to GND)
CID_DATA[2:0]	0D:[10:8]	X	Output of Caller ID comparator circuit. Most recent three bits, sampled at 48 kHz. (Bit 2 is oldest).
DAC[3:0]	03:[11:8]	0	Controls signal gain to DAC in 4 steps: 0, -10, -15, -22.5 dB.
DAC[5:0]	0C:[13:8]	00h	6-bit DC Control DAC output. Used for DC current control and Ring Threshold.
DAC1	01:3	X	16-bit Sigma Delta DAC circuit ready indicator at cold start/reset. '1' = DAC ready. '0' = DAC not ready.
DASEL[1:0]	0C:[6:4]	000	6-bit DC control DAC output select. '000' - '111' = Undefined.
DATAMODE	0A:12	0	Tip & Ring monitor mode enable. Controls Data2 packet content for DIB. '1' = Copy TRSTAT to Data2/Data2bis packets '0' = Use RX word from 16-bit ADC for Data2/Data2bis.
DM1	0A:13	1	Dither enable for modem ADC. '1' = Dither circuit enabled. '0' = Dither circuit disabled.
EIC0	0C:7	1	Control time constant for Electronic Inductor for Tip & Ring. '1' = Undefined. '0' = Undefined.
GC	4:[15:0]	FFh	GPIO Pin Direction configuration mask register. '1' = GPIOx is an Input. '0' = GPIOx is an output.

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GCS	6:[15:0]	00h	GPIO Pin Sticky configuration mask register. '1' = GPIx is non-sticky (level sensitive) '0' = GPIx is sticky (edge sensitive).
GI	08:[15:0]	XXh	GPIO Pin Status register. '1' = GPIx (level sensitive) is active, or GPIx (edge sensitive) has detected an edge, or GPOx output is high. '0' = GPIx is inactive (no edge) or output low.
GP	05:[15:0]	FFh	GPIO Pin Polarity/Type configuration mask register. '0' = Low active/CMOS output '1' = high active/open-drain output.
GPIO	1:0	X	GPIO circuit ready indicator at cold start/reset. '1' = GPIO ready. '0' = GPIO not ready.
GW	07:[15:0]	00h	GPIO Pin Wake up configuration mask register. '0' = No interrupt on GPIO activity '1' = Interrupt on GPIO activity.
L1B[2:0]	0A:[10:8]	000	Modem Line Loop Back Control. '000' = Normal operation '001' = ADC loop back '010' = Local Analog loop back '011' = DAC loop back '100' = Remote Analog loop back '101' = ADC and DAC loop back combined '110' = DAC one bit out '111' = SCF one bit in.
LCL	0B:14	X	Line Current Loss indicator. '0' = Normal '1' = Line Current is zero even though EI is trying to draw current from Telco.
LM1[1:0]	0A:[7:6]	00	Modem Line TX low pass filter pole location. '00' = 8 kHz '01' = 12 kHz '10' = 25 kHz '11' = 25 kHz.
-LPR	0D:4	X	Output of LPR Detector (comparator). Either RDO/LPR or -LPR will be 1 when Line Polarity Reversal is received.
Mref	1:1	X	Modem Reference Voltage circuit ready indicator at cold start/reset. '1' = Mref ready. '0' = Mref not ready.
Mute ADC	3:7	1	Mutes Sigma-Delta ADC input. '1' = Mute enabled. '0' = Mute disabled.

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Mute DAC	3:15	1	Mutes Sigma-Delta DAC output. '1' = Mute enabled. '0' = Mute disabled.
~OH	0A:14	1	Off Hook Control bit. '1' = On hook '0' = Off hook (drawing line current).
PRA	1:8	1	Power control for GPIO
PRB	1:9	1	Power control for Modem Voltage Reference
PRC	1:10	1	Power control for Sigma-Delta ADC
PRD	1:11	1	Power control for Sigma-Delta DAC
~RD/CID	0B:7	0	Ring Detect/CID Detect Select bit. '0' = Ring Detector active '1' = CID detector active.
RDO/LPR	0D:0	X	Output of Ring Detect Comparator/LPR Detector.
RDY	0B:15	X	Ready Status bit. '1' = 7-bit monitor ADC value ready. '0' = 7-bit ADC not ready.
Rev[5:0]	11:[5:0]	00	Revision code for Line Side Device. First device will use 000000.
RXGAIN	0A:11	1	6 dB Digital Gain control for ADC output. '1' = +6 dB to ADC word. '0' = 0 dB applied to ADC word.
SCM1	0A:5	0	Modem Line TX SCF gain control. '0' = 0 dB gain '1' = 6 dB gain.
SR	2:[7:0]	2Fh	Oversampling Ratio (OSR) for Sigma-Delta codec. '2F' = 16 kHz sampling rate.
TEST1	0F:[15:0]	XX	TEST register – reserved for tests.
TEST2	10:[15:0]	XX	TEST register – reserved for tests.
TXM	0A:15	0	Transmit path enable. '1' = Modem transmit path enabled. '0' = Modem transmit path disabled.
USZ[1:0]	0C:[15:14]	11	US Virtual Impedance Enable/Disable '11' = US VI Enabled. '00' = US VI Disabled.

VCR	0D:12	X	Output of Voltage Clamp circuit. '1' = Circuit is actively clamping Vdd.
VM1[1:0]	0A:[4:3]	00	Modem Line DAC interpolator gain. '00' = 0 dB '01' = 6 dB gain '10' = 12 dB gain '11' = -6 dB gain.
WZ[2:0]	0C:[2:0]	000	World Wide Virtual Impedance Enable/Disable '11' = WW VI Enabled. '00' = WW VI Disabled.

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What is claimed is:

1. A data access arrangement, comprising:

a high voltage isolation barrier having a first side and a second side;

system side circuitry coupled to the first side of the high voltage isolation barrier, the system side circuitry configurable to communicate with host system circuitry; and

line side circuitry coupled to the second side of the high voltage isolation barrier, the line side configurable to communicate with a telephone network,

wherein information is communicated bidirectionally between the system side circuitry and the line side circuitry across the high voltage isolation barrier in a digital format.

2. The data access arrangement of claim 1, wherein the high voltage isolation barrier comprises a capacitor.

3. The data access arrangement of claim 2, wherein the high voltage isolation barrier further comprises a transformer having a primary side coupled to the system side circuitry and a secondary side coupled to the line side circuitry, the transformer configurable to provide power from the system side circuitry to the line side circuitry.

4. The data access arrangement of claim 2, wherein the high voltage isolation barrier further comprises a transformer having a primary side coupled to the system side circuitry and a secondary side coupled to the line side circuitry, the transformer configurable to provide a clock signal from the system side circuitry to the line side circuitry.

5. The data access arrangement of claim 1, wherein the high voltage isolation barrier comprises a first capacitor and a second capacitor.

6. The data access arrangement of claim 5, wherein the system side circuitry comprises a first transceiver circuit for bidirectional communications with the high voltage isolation barrier, and wherein the line side circuitry comprises a second transceiver circuit for bidirectional communications with the high voltage isolation barrier, the first and second transceiver circuits configured to transmit/receive differential signals across the first and second capacitors to communicate digital information.

7. The data access arrangement of claim 5, the high voltage isolation barrier further comprising a transformer having a primary side coupled to the system side circuitry and a secondary side coupled to the line side circuitry, the transformer configurable to provide power from the system side circuitry to the line side circuitry.

8. The data access arrangement of claim 5, the high voltage isolation barrier further comprising a transformer having a primary side coupled to the system side circuitry and a secondary side coupled to the line side circuitry, the transformer configurable to provide a clock signal from the system side circuitry to the line side circuitry.

9. The data access arrangement of claim 1, wherein the high voltage isolation barrier comprises a transformer.

10. The data access arrangement of claim 1, wherein the high voltage isolation barrier comprises an opto-coupler circuit.

11. The data access arrangement of claim 1, wherein the line side circuitry includes a coder/decoder, and wherein the

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digital information communicated between the system side circuitry and the line side circuitry includes encoded information generated by the coder/decoder and information for decoding by the coder/decoder.

12. The data access arrangement of claim 1, wherein the line side circuitry includes a programmable detection circuitry for detecting predetermined conditions on a telephone network, and wherein the digital information communicated between the system side circuitry and the line side circuitry includes information for programming a predetermined threshold of the detection circuitry.

13. A computer system, comprising:

a data bus;

a processor coupled to the data bus; and

a modem coupled to the data bus, the modem comprising:
a high voltage isolation barrier having a first side and a second side;

system side circuitry coupled to the first side of the high voltage isolation barrier, the system side circuitry configurable to communicate with host system circuitry; and

line side circuitry coupled to the second side of the high voltage isolation barrier, the line side configurable to communicate with a telephone network,

wherein information is communicated bidirectionally between the system side circuitry and the line side circuitry across the high voltage isolation barrier in a digital format.

14. The computer system of claim 13, wherein the high voltage isolation barrier comprises a capacitor.

15. The computer system of claim 14, the high voltage isolation barrier further comprising a transformer having a primary side coupled to the system side circuitry and a secondary side coupled to the line side circuitry, the transformer configurable to provide power from the system side circuitry to the line side circuitry.

16. The computer system of claim 14, the high voltage isolation barrier further comprising a transformer having a primary side coupled to the system side circuitry and a secondary side coupled to the line side circuitry, the transformer configurable to provide a clock signal from the system side circuitry to the line side circuitry.

17. The computer system of claim 13, wherein the high voltage isolation barrier comprises a first capacitor and a second capacitor.

18. The computer system of claim 17, wherein the system side circuitry comprises a first transceiver circuit for bidirectional communications with the high voltage isolation barrier, and wherein the line side circuitry comprises a second transceiver circuit for bidirectional communications with the high voltage isolation barrier, the first and second transceiver circuits configured to transmit/receive differential signals across the first and second capacitors to communicate digital information.

19. The computer system of claim 13, wherein the line side circuitry includes a coder/decoder, wherein the digital information communicated between the system side circuitry and the line side circuitry includes encoded information generated by the coder/decoder and information for decoding by the coder/decoder.

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United States Patent [19]

Hill et al.

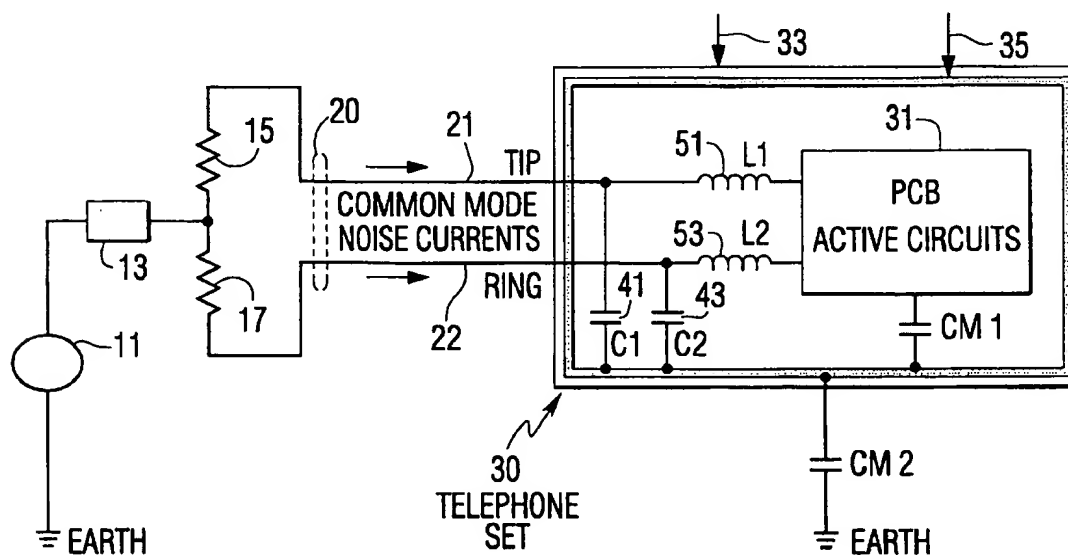
[11] **Patent Number:** 5,642,416[45] **Date of Patent:** Jun. 24, 1997[54] **AM BROADCAST BAND INTERFERENCE
FILTER FOR LINE-POWERED TELEPHONE**[75] **Inventors:** Ralph Leon Hill, Pepperell, Mass.;
Noel C. Pratt, Van Nuys, Calif.[73] **Assignee:** Harris Corporation, Melbourne, Fla.[21] **Appl. No.:** 399,355[22] **Filed:** Mar. 3, 1995[51] **Int. Cl.⁶** H04M 1/74; H04B 1/10[52] **U.S. Cl.** 379/416; 379/399; 379/414;
379/412; 379/429; 455/296[58] **Field of Search** 455/300, 301,
455/296; 379/416, 415, 417, 414, 412,
429, 399; 178/63 E; 381/189[56] **References Cited****U.S. PATENT DOCUMENTS**

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Primary Examiner—Krista M. Zele*Assistant Examiner*—Devendra T. Kumar*Attorney, Agent, or Firm*—Charles E. Wands[57] **ABSTRACT**

An electromagnetic interference by-pass filtering mechanism suppresses RF noise currents conducted over the tip and ring leads of a telephone line-powered telephone instrument. Such RF noise currents may result from amplitude modulated radio broadcast signals emanating in the vicinity of the telephone instrument. The filtering mechanism comprises a conductive material coated on the interior surface of the housing of the telephone instrument, so as to surround the printed circuit board containing the telephone circuitry of the instrument. The conductive material is coupled to earth. First and second capacitors are coupled between the tip and ring leads and the conductive material, and first and second inductors are coupled in series with the tip and ring conductors and connections of the tip and ring conductors to the printed circuit board containing the telephone circuitry.

19 Claims, 1 Drawing Sheet

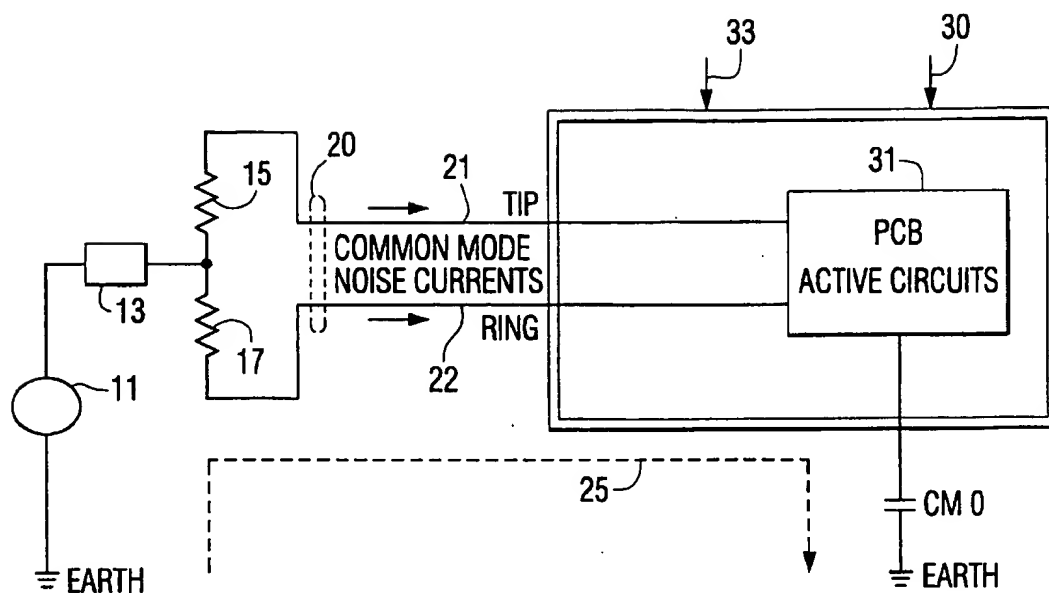


FIG. 1
PRIOR ART

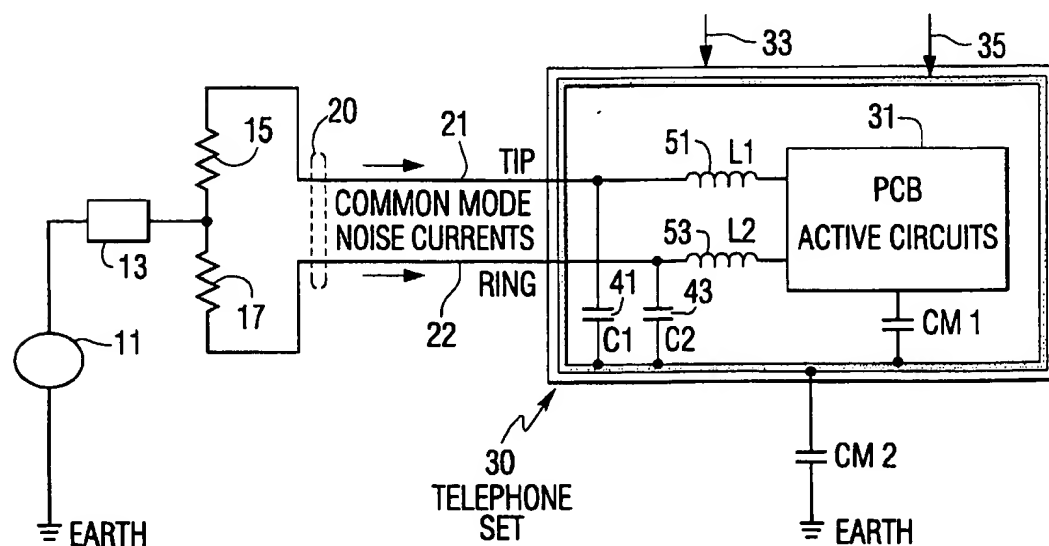


FIG. 2

AM BROADCAST BAND INTERFERENCE FILTER FOR LINE-POWERED TELEPHONE

FIELD OF THE INVENTION

The present invention relates in general to communication systems and devices, and is particularly directed to a mechanism installable in a telephone line-powered telephone instrument for suppressing AM broadcast band (typically defined from 540 KHz to 1800 KHz) electromagnetic interference (EMI) that is conducted along wires into a telephone line-powered telephone instrument.

BACKGROUND OF THE INVENTION

Electromagnetic interference (EMI), which involves the undesired coupling of electromagnetic energy from an electromagnetic energy source to an affected circuit, system, or structure, may be coupled from the source in one of four ways: 1- through conduction along wires; 2- by far field radiation, such as occurs between a transmitting antenna and a receiving antenna separated by approximately one or more wavelengths of the interference frequency; 3- through capacitive (electric field) coupling; and 4- through inductive (magnetic field) coupling.

One example of the EMI problem involves the widespread use of digital computer circuits in automobile control systems. Such circuits are vulnerable to EMI from radio frequency transmitters such as cellular telephones and amateur radio ("ham") transmitters. In order to function properly, the electronic engine and braking system computers within an automobile must be designed to be relatively immune to the influence of the electromagnetic fields generated by such nearby transmitters.

Similarly, telephone instruments, such as ruggedized test telephones, are often used in an environment that includes one or more nearby AM broadcast radio stations having high power radio frequency transmitters and associated antenna systems, and are therefore subject to exposure to electromagnetic energy that may be sufficient to interfere with or completely disable the operation of such an instrument. Field experience of the present inventors has shown that interference to telephones caused by AM radio broadcasts results mainly from radiated RF signals that are coupled into nearby telephones transmission lines and are then conducted as RF currents into telephones connected to the affected transmission lines.

Because most present day telephone designs employ active circuits (amplifiers, automatic gain control circuits, etc.), which provide telephones with certain advantages over the older "passive" designs, they have greater susceptibility to interference caused by unwanted RF currents. This is due to the nature of the active circuitry which has the undesired capability of readily demodulating audio from amplitude modulated RF carriers.

Field experience in the vicinity of AM radio stations has shown that interference to the desired operation of a telephone instrument is manifested in two primary ways: 1- the telephone's electronic circuits demodulate the audio signal component of amplitude modulated RF currents, amplify this unwanted audio signal component, and couple it to the telephone's receiver, thereby making it extremely difficult or effectively impossible to understand intended received speech; and 2- if the RF signal strength is high enough, the internal circuitry of the telephone instrument will be disabled, making it impossible to place a call.

This problem is diagrammatically illustrated in FIG. 1, which shows a circuit equivalent of high powered,

commercial, radio broadcast antenna, transmitting RF signals into a two wire, metallic, telephone transmission line located in the vicinity of the antenna transmitter site. The unwanted AM broadcast signal is schematically represented by a noise source 11 having an associated noise source impedance 13. The AM signal is injected through a pair of resistors 15 and 17, that represent a balanced two-wire transmission line 20, to tip and ring connectors 21 and 22 of a telephone set 30. The hardware of telephone set 30 typically includes a printed circuit board 31, housed within an insulating (plastic) housing or case 33. Mounted on printed circuit board 31 are one or more active electronic circuits, which are capacitively coupled to earth by a naturally occurring mutual capacitance CMO. The undesired RF currents are conducted over the two wire (tip and ring) transmission line 20 in common mode fashion.

RF noise tests conducted in the field have revealed that the strength of the RF noise signal, which follows the dotted line path 25 (from the source 11—through tip and ring transmission line 20—the amplifier circuitry of printed circuit board 31—mutual capacitance CMO-to-earth) is high enough to cause interference to the telephone instrument for blocks around the perimeter of an AM radio broadcast facility.

Presently, in the United States, there are no mandatory regulations requiring manufacturers to provide RF immunity in telephone sets. Although the FCC does not regulate RF susceptibility in telephone equipment, it is aware that RFI in telephones is a problem. In 1994, the FCC published the results of an informal field survey on RF interference to telephones in which several field offices tested the susceptibility of various types of telephones at over a hundred locations of reported RFI. In its report, the FCC describes using a "bulletproof" telephone, having a passive design (which is inherently more immune to RF currents than designs employing active circuits, as noted above) that employs LC filtering to reduce RFI.

On the other hand, there are already several European countries that require compliance of telephone equipment with RF immunity specifications. European specifications require that compliance be demonstrated by laboratory testing. There are two consequences of this that will affect the nature of RF filter designs. First, laboratory conditions do not necessarily duplicate the conditions in the field; secondly, specified test levels are considerably lower than those experienced in the field, especially when the telephone is in close proximity to high powered broadcast facilities. Thus solutions to RFI which work in a lab at relatively low test levels will likely be different than those which successfully operate in a practical or 'real world' environment.

In addition, in Mexico, Telefonos de Mexico (TelMex) has a requirement that telephones must have RF Immunity. To date the present inventors have not experienced the use of any telephones in Mexico that completely suppresses RFI. Either or both of the fundamental problems described above are typical, AM audio signals are demodulated or the telephone's electronic circuitry is affected (e.g., dialing circuitry disabled by conducted RF current).

Although various shielding/grounding schemes, such as those described in the U.S. Patents to Pesola et al, No. 5,271,056 and Bogese, No. 4,738,638, address the EMI problem in general, neither patent describes the above-referenced problem of unwanted demodulation by the telephone's electronic circuitry of AM broadcast signals as undesired common mode RF currents on the two wire (tip and ring) conductors. The Pesola et al patent describes the use of a ground foil with a raised edge of frame plate for

components of a radio telephone. The Bogese patent describes the replacement of one of the conductors of a telephone type modular jack with a ground strap having a wide surface for conducting high frequency EMI signals to ground, or a metallic connector cover provided for the purpose.

SUMMARY OF THE INVENTION

The present invention is directed to a mechanism that effectively eliminates interference caused by high level, amplitude modulated, radio broadcasts, in particular, to the elimination of radio frequency interference (RFI) resulting from amplitude modulated, conducted, RF noise currents on the tip and ring conductors to a telephone set's active circuits. As will be described, the invention is operative to filter out conducted AM radio current signals such that the filtered telephone can perform its expected operations, there is no interference with conversation, and there is no degradation of conventional telephone performance parameters.

For this purpose, the invention involves modifying a conventional telephone set to include a conductive coating applied to the interior surface of its insulating case. In addition, coupled between the tip and ring conductors and the conductive coating of the case are first and second auxiliary capacitors, while first and second inductors are coupled in series with the tip and ring conductors and their connections to the printed circuit board.

Each of the auxiliary capacitors has a value that is considerably larger than the value of mutual capacitance between conductive traces on printed circuit board and the conductive coating on the interior of the telephone's case. The effective impedance to earth seen by common mode RF noise current signals on the tip and ring leads is therefore far lower than that encountered in a path through the circuitry on the printed circuit board. Although this effectively increases the common mode current injected into the telephone, the lower impedance of the by-pass path through the auxiliary capacitors steers the common mode RF current around the printed circuit board, rather than through its active circuitry.

The values of the auxiliary capacitors must be sufficiently small to prevent reduction of the AC impedance that the telephone presents to the telephone network, when it is off hook. It has been found that each of the auxiliary capacitors may have a value on the order of 0.02 uf or less. When looking into the telephone circuit across the tip and ring leads, the auxiliary capacitors are in series with each other and establish a capacitance on the order of 0.01 uf across tip and ring, which is in parallel with the impedance of the telephone set. Capacitor values considerably larger than 0.02 uf may reduce the AC impedance of the telephone set to below the required 600 to 900 ohm range, which must be maintained over the 300 to 3400 Hz speech band. Although increasing the values of the pair of auxiliary tip and ring capacitors to values larger than 0.02 uf further reduces the level of demodulated audio, doing so would compromise the effective AC impedance.

The inductors present a high series impedance to the RF noise signals and thereby further reduces RF current into the telephone's active circuits, so that the level of the demodulated audio noise signal is below human audibility level. This effectively makes the performance of the telephone under test, modified in accordance with the present invention, virtually indistinguishable from telephones connected to transmission lines in which no RF current is flowing.

BRIEF DESCRIPTION OF THE DRAWINGS

FIG. 1 diagrammatically illustrates a circuit equivalent of high powered, commercial, radio broadcast antenna, transmitting RF signals that are readily picked up by two wire, metallic, telephone transmission lines located in the vicinity of a broadcast antenna site; and

FIG. 2 diagrammatically shows a modification of the configuration of a telephone set to include a conductive coating, auxiliary parallel tip and ring capacitors, and series inductors in accordance with the invention.

DETAILED DESCRIPTION

As described briefly above, the RFI filter mechanism of the present invention is operative to effectively eliminate interference caused by high level, amplitude modulated, radio broadcasts, in particular, radio frequency interference (RFI) resulting from amplitude modulated RF noise currents conducted over the tip and ring leads to the active circuitry components of a telephone set, so that there is no degradation of conventional telephone performance parameters.

The present invention is diagrammatically illustrated in FIG. 2, which shows a modification of the configuration of a telephone set 30 to include a conductive coating 35 applied to the interior surface of its insulating (plastic) housing or case 33. In addition, coupled between the tip and ring conductors 21 and 22 of transmission line 20 and conductive coating 35 are first and second auxiliary capacitors 41 and 43, having respective values C1 and C2. Also, first and second auxiliary inductors 51 and 53 (having respective values L1 and L2 of approximately 1 mH each) are coupled in series with the tip and ring conductors 21 and 22 and their connections to printed circuit board 31.

The respective values C1 and C2 of auxiliary capacitors 41 and 43 are considerably larger than the value of mutual capacitance CM1 between conductive traces on printed circuit board 31 and the conductive coating 35 within the telephone set case 33. The mutual capacitance between conductive coating 35 and earth is denoted by CM2. As a result, the effective impedance to earth seen by the common mode RF noise current signals on the tip and ring leads 21 and 22 is far lower than that encountered in a path through the circuitry on the printed circuit board 31.

Although the conductive coating and LC by-pass arrangement of the present invention may increase the common mode current injected into the telephone, the lower impedance of the 'by-pass' path through auxiliary capacitors 41 and 43 serves to direct the common mode RF current around the printed circuit board 31, rather than through an 'undesired' path that includes the active circuitry on the printed circuit board 31. The values of auxiliary capacitors 41 and 43 must be sufficiently small to prevent reduction of the AC impedance that the telephone presents to the telephone network, when it is off hook.

As a non-limiting example it has been found that each of auxiliary capacitors 41 and 43 may have a value on the order of 0.02 uf or less. As noted earlier, when looking into the telephone circuit across the tip and ring leads 21 and 22, auxiliary capacitors 41 and 43 are in series with each other and establish a capacitance on the order of 0.01 uf across the tip and ring conductors 21 and 22. This resulting AC impedance is in parallel with the AC impedance of the telephone set. Capacitor values significantly larger than 0.02 uf may reduce the AC impedance of the telephone set to below the required 600 to 900 ohm range (which must be maintained over the 300 to 3400 Hz speech band). If the

Use for chassis ground

values of auxiliary capacitors 41 and 43 are larger than 0.02 uf, the level of demodulated audio can be further reduced; however, doing so would compromise the effective AC impedance.

The effect of inductors 51 and 53 is to present a high series impedance to the RF noise signals and thereby further reduce the injection of RF current into the telephone's active circuits, so that the level of the audio noise signal is below human audibility level. This effectively makes the performance of the telephone modified in accordance with the present invention virtually indistinguishable from a telephone connected to a transmission line in which no RF current is flowing.

As will be appreciated from the foregoing description, the auxiliary by-pass filtering mechanism of the present invention is operative to eliminate interference caused by high level, amplitude modulated, radio broadcasts, in particular, radio frequency interference (RFI) resulting from amplitude modulated RF noise currents conducted over the tip and ring leads of a telephone line-powered telephone instrument, so that the filtered telephone circuitry can perform its expected operations, without interference with conversation, and without degradation of conventional telephone performance parameters. What results is a telephone set that is virtually indistinguishable from one connected to transmission lines in which no RF current is flowing.

While we have shown and described an embodiment in accordance with the present invention, it is to be understood that the same is not limited thereto but is susceptible to numerous changes and modifications as known to a person skilled in the art, and we therefore do not wish to be limited to the details shown and described herein but intend to cover all such changes and modifications as are obvious to one of ordinary skill in the art.

What is claimed:

1. An arrangement for suppressing interference caused by amplitude modulated radio frequency (RF) noise currents conducted over tip and ring leads to a telephone instrument, so that telephone circuitry of the telephone instrument can perform its expected operations without interference with conversation, and without degradation of telephone performance parameters, said arrangement comprising a conductive material supported within a housing of said telephone instrument, such that said conductive material surrounds said telephone circuitry of said telephone instrument, said conductive material being capacitively coupled to earth, and first and second capacitors coupled between said tip and ring leads and said conductive material.

2. An arrangement according to claim 1, wherein respective values of said first and second capacitors are larger than the value of mutual capacitance between conductors of said telephone circuitry and said conductive material, so that the effective impedance to earth seen by common mode RF noise current signals conducted on said tip and ring leads is lower than that encountered in a path through said telephone circuitry.

3. An arrangement according to claim 1, wherein respective values of said first and second capacitors are sufficiently small to prevent a significant reduction of the AC impedance that said telephone circuitry presents to a telephone network when said telephone instrument is off-hook.

4. An arrangement according to claim 1, wherein each of said first and second capacitors has a value on the order of 0.02 uf or less.

5. An arrangement according to claim 1, wherein said conductive material comprises a conductive coating formed on an interior surface of said housing of said telephone instrument.

6. An arrangement according to claim 5, further comprising first and second inductors coupled in series with said tip

and ring leads and connections of said tip and ring leads to said telephone circuitry of said telephone instrument.

7. An arrangement according to claim 1, further comprising first and second inductors coupled between said tip and ring leads and said telephone circuitry of said telephone instrument.

8. An arrangement according to claim 7, wherein said first and second inductors have values on the order of 1 mH.

9. An arrangement according to claim 8, wherein each of said first and second capacitors has a value on the order of 0.02 uf or less.

10. An arrangement for suppressing interference caused by amplitude modulated radio frequency noise currents conducted over tip and ring leads to a telephone instrument, so that telephone circuitry of the telephone instrument can perform its expected operations without interference with conversation, and without degradation of telephone performance parameters, said arrangement comprising a conductive material supported within a housing of said telephone instrument, such that said conductive material surrounds said telephone circuitry of said telephone instrument, said conductive material being capacitively coupled to earth, and first and second inductors coupled between said tip and ring leads and said telephone circuitry.

11. A method for suppressing interference in the operation of telephone circuitry of a telephone instrument caused by radio frequency (RF) noise currents, conducted over tip and ring leads to said telephone instrument, as a result of AM broadcast signals from an AM radio source in the vicinity of said telephone instrument, said method comprising the steps of:

(a) surrounding said telephone circuitry of said telephone instrument with a conductive material which is capacitively coupled to earth; and

(b) coupling first and second capacitors between said tip and ring leads and said conductive material.

12. A method according to claim 11, wherein respective values of said first and second capacitors are larger than the value of mutual capacitance between conductors of said telephone circuitry and said conductive material, so that the effective impedance to earth seen by common mode RF noise current signals conducted on said tip and ring leads is lower than that encountered in a path through said telephone circuitry.

13. A method according to claim 11, wherein respective values said first and second capacitors are sufficiently small to prevent a significant reduction of the AC impedance that said telephone circuitry presents to a telephone network when said telephone instrument is off-hook.

14. A method according to claim 11, wherein each of said first and second capacitors has a value on the order of 0.02 uf or less.

15. A method according to claim 11, wherein step (a) comprises forming said conductive material as a conductive coating on an interior surface of a housing of said telephone instrument.

16. A method according to claim 15, further comprising the step (c) of installing first and second inductors between said tip and ring leads and said telephone circuitry of said telephone instrument.

17. A method according to claim 11, further comprising the step (c) of installing first and second inductors between said tip and ring leads and said telephone circuitry of said telephone instrument.

18. A method according to claim 17, wherein said first and second inductors have values on the order of 1 mH.

19. A method according to claim 18, wherein each of said first and second capacitors has a value on the order of 0.02 uf or less.

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